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Devices Connected/Referenced

AD7124-4	Low Power, 24-Bit, Sigma-Delta ADC with PGA and Reference
AD5421	16-Bit, Loop Powered, 4 mA to 20 mA DAC
AD5700	Low Power HART Modem
ADuM1441	SPI Isolator
ADP162	Ultralow Quiescent Current, 150 mA, CMOS Linear Regulator
ADG5433	High Voltage Latch-Up Proof, Triple SPDT Switches

Isolated 4 mA to 20 mA/HART Temperature and Pressure Industrial Transmitter Using a Low Power, Precision, 24-Bit, Sigma-Delta ADC

EVALUATION AND DESIGN SUPPORT

Circuit Evaluation Board

[DEMO-AD7124-DZ Evaluation Board](#)

Design and Integration Files

[Schematics, Layout Files, Bill of Materials, Code Examples](#)

CIRCUIT FUNCTION AND BENEFITS

The circuit shown in Figure 1 is an isolated smart industrial field instrument that interfaces to many types of analog sensors such as temperature (Pt100, Pt1000, and thermocouple) or bridge pressure sensors. The instrument communicates via a 4 mA to 20 mA analog output and a highway addressable remote transducer (HART®) interface. HART is a digital 2-way communication in which a 1 mA peak-to-peak frequency shift keyed (FSK) signal is modulated on top of the standard 4 mA to

20 mA analog current signal. The HART interface allows features such as remote calibration, fault interrogation, and transmission of process variables, which are necessary in applications such as temperature and pressure control.

The circuit uses the [AD7124-4](#), an ultralow power, precision 24-bit, Σ - Δ analog-to-digital converter (ADC), which includes all the features needed for temperature and pressure systems. The circuit also includes the [AD5421](#), a 16-bit, 4 mA to 20 mA, loop powered digital-to-analog converter (DAC); the [AD5700](#), the industry's lowest power and smallest footprint HART-compliant IC modem; the [ADuM1441](#), which provides ultralow power serial peripheral interface (SPI) isolation; the [ADG5433](#) CMOS switch; and the [ADP162](#) low power, 3.3 V regulator in the isolated power circuitry.

Rev. A

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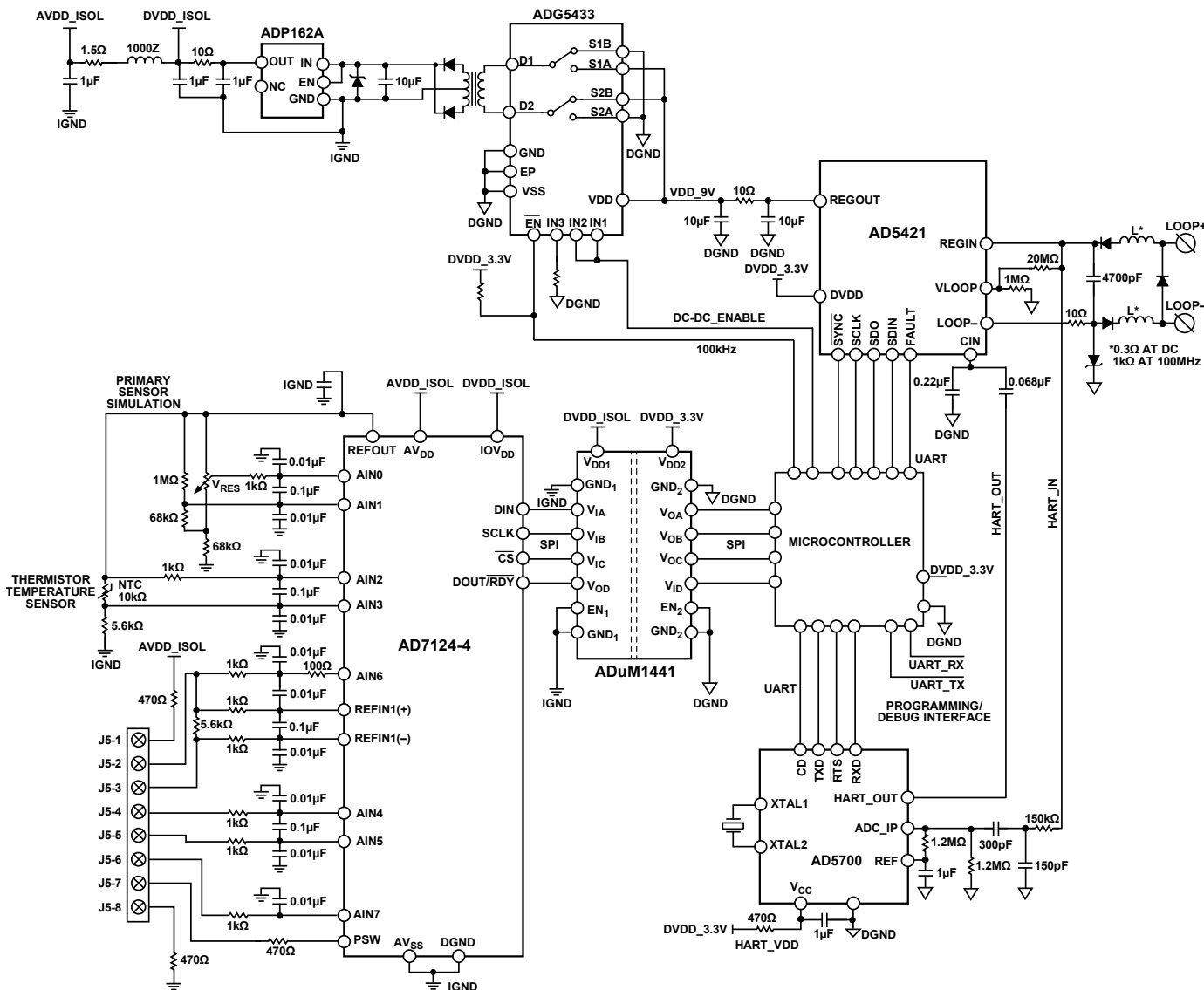


Figure 1. 4 mA to 20 mA, Loop Powered Field Instrument with HART Interface (Simplified Schematic: All Connections and Decoupling Not Shown)

CIRCUIT DESCRIPTION

Analog Front-End Interface

The **AD7124-4** is a low power, low noise, completely integrated analog front end for high precision measurement applications. The device contains a low noise, 24-bit, Σ - Δ analog-to-digital converter (ADC), and can be configured to have four differential inputs or seven single-ended or pseudo differential inputs. The on-chip low noise gain stage ensures that signals of small amplitude can be interfaced directly to the ADC.

One of the major advantages of the **AD7124-4** is that it gives the user the flexibility to employ one of three integrated power modes. The current consumption, range of output data rates, and rms noise can be tailored with the power mode selected. The device also offers a multitude of filter options, ensuring that the user has the highest degree of flexibility.

The **AD7124-4** can achieve simultaneous 50 Hz and 60 Hz rejection when operating at an output data rate of 25 SPS (single-cycle settling).

The **AD7124-4** establishes the highest degree of signal chain integration. The device contains a precision, low noise, low drift internal band gap reference, and also accepts an external differential reference, which can be internally buffered. Other key integrated features include programmable low drift excitation current sources, burnout currents, and a bias voltage generator, which sets the common-mode voltage of a channel to $AV_{DD}/2$. The low-side power switch enables the user to power down bridge sensors between conversions, ensuring the absolute minimal power consumption of the system. The device also allows the user the option of operating with either an internal clock or an external clock.

The integrated channel sequencer allows several channels to be enabled simultaneously, and the AD7124-4 sequentially converts on each enabled channel, simplifying communication with the device. As many as 16 channels can be enabled at any time; a channel being defined as an analog input or a diagnostic such as a power supply check or a reference check. This unique feature allows diagnostics to be interleaved with conversions. The AD7124-4 also supports per channel configuration. The device allows eight configurations or setups. Each configuration consists of gain, filter type, output data rate, buffering, and reference source. The user can assign any of these setups on a channel by channel basis.

The AD7124-4 also has extensive diagnostic functionality integrated as part of its comprehensive feature set. These diagnostics include a cyclic redundancy check (CRC), signal chain checks, and serial interface checks, which lead to a more robust solution. These diagnostics reduce the need for external components to implement diagnostics, resulting in reduced board space needs, reduced design cycle times, and cost savings. The failure modes effects and diagnostic analysis (FMEDA) of a typical application has shown a safe failure fraction (SFF) greater than 90% according to IEC 61508.

Sensor Input

The circuit supports 3-wire and 4-wire RTDs, thermocouples, and pressure transducers via the 8-pin connector. The AD7124-4 has all the building blocks needed to interface to these sensors. For all the sensor types connected, the ADC is used in mid power mode. The post filter is used because it enables simultaneous 50 Hz and 60 Hz rejection when converting at 25 SPS. When a sensor is connected to the circuit, the ADC is configured to suit the sensor type connected. An internal full-scale and offset calibration can also be performed to minimize the offset error and full-scale error, the calibrations being initiated by a UART or HART command.

The AD7124-4 has numerous diagnostics on-chip, which ensure a robust design. In this circuit, open-wire detection ensures that the sensors are connected, the power-on reset (POR) in the status register is monitored so that the user is informed when a power-on reset occurs. The error register is read for each conversion, and its contents are sent via HART along with the sensor result.

RTD

A resistive temperature detector (RTD) can measure temperature from -200°C to $+600^{\circ}\text{C}$. Typical RTDs are Pt100 and Pt1000 and are made of platinum. A Pt100 is used with this circuit.

4-Wire RTD

Figure 2 shows how a 4-wire Pt100 RTD connects to the circuit.

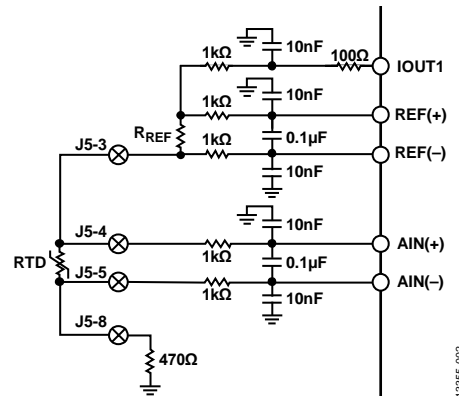


Figure 2. 4-Wire RTD

One of the on-chip excitation currents of the AD7124-4 excites the Pt100. The maximum resistance of the Pt100 is $313.71\ \Omega$ at 600°C . If the excitation current is programmed to $250\ \mu\text{A}$, the maximum voltage generated across the Pt100 is

$$250\ \mu\text{A} \times 313.71\ \Omega = 78.43\ \text{mV}$$

With the programmable gain array (PGA) programmed to a gain of 16, the maximum voltage seen at the modulator input is

$$78.43\ \text{mV} \times 16 = 1.25\ \text{V}$$

A $5.6\ \text{k}\Omega$ precision resistor (0.05%, 10 ppm/ $^{\circ}\text{C}$) generates the reference voltage. The value of the reference resistor, R_{REF} , is chosen so that the voltage generated across it has a minimum value of 1.25 V in this circuit, that is, the voltage seen at the modulator input due to the analog input is less than or equal to the reference voltage. The $250\ \mu\text{A}$ current that supplies the Pt100 also flows through the $5.6\ \text{k}\Omega$ resistor, resulting in a ratiometric configuration. Therefore, any variation of the excitation current has no effect on the performance of the circuit. The voltage generated across the precision resistor is

$$5.6\ \text{k}\Omega \times 250\ \mu\text{A} = 1.4\ \text{V}$$

Antialiasing filters are included on the analog input and reference input. These filters prevent any interference at multiples of the modulator sampling frequency aliasing into the band of interest. To ensure that these filters and the external resistors do not cause gain errors, the reference buffers are enabled. The analog input buffers are enabled automatically because these buffers are enabled when the PGA is used. The reference buffers require some headroom (100 mV within the power supply rails). Therefore, a $470\ \Omega$ resistor was included on the low side to allow this headroom.

The $250\ \mu\text{A}$ excitation current requires 370 mV of headroom. The voltage seen on this pin is $(470 + 5600 + 313.71)\ \Omega \times 250\ \mu\text{A} = 1.6\ \text{V}$, which is acceptable.

The AIN4 and AIN5 pins are used as the AINP and AINM analog input.

The 1 kΩ resistors on the connector pins have a dual purpose: they make up the antialias filters, and they also protect the analog inputs if an overvoltage occurs (due to miswiring, for example).

The [Circuit Note CN-0381](#) provides further detail on interfacing 4-wire Pt100 sensors to the [AD7124-4](#) and linearizing or post-processing the conversions.

The circuit shown in Figure 1 also supports a 4-wire Pt1000 RTD. The circuit connections are the same as those used for the Pt100. The ADC configuration used is described previously in this section, but with the PGA gain set to 1.

3-Wire RTD

Figure 3 shows how a 3-wire Pt100 RTD connects to the circuit.

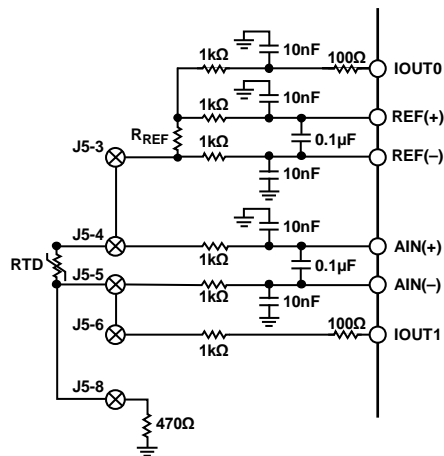


Figure 3. 3-Wire RTD

The [AD7124-4](#) has two matched excitation currents. Both are used with the 3-wire RTD so that lead wire compensation can be performed. Because the Pt100 has a maximum resistance is 313.71 Ω (at 600 °C), the excitation currents are programmed to 250 μA. The reference resistor, R_{REF}, is connected on the top side. Therefore, one 250 μA excitation current (IOUT0) is output on Pin AIN6, flows through the 5.6 kΩ precision reference resistor (0.05%, 10ppm/°C), and then through the Pt100. The second 250 μA current (IOUT1) is output on pin AIN7. This current generates a voltage due to the lead resistance, which is in opposition to the lead resistance voltage generated due to the current on AIN6. Therefore, the error due to the lead resistance is minimized.

The voltage generated across the 5.6 kΩ reference resistor is

$$250 \mu\text{A} \times 5.6 \text{ k}\Omega = 1.4 \text{ V}$$

The maximum voltage generated across the Pt100 is

$$250 \mu\text{A} \times 313.71 \Omega = 78.43 \text{ mV}$$

With the PGA programmed to a gain of 16, the voltage seen at the modulator of the [AD7124-4](#) is

$$78.43 \text{ mV} \times 16 = 1.25 \text{ V}$$

This voltage is within range because it is less than the reference voltage.

Antialiasing filters are included on the analog input and reference input. These filters prevent any interference at multiples of the modulator sampling frequency from aliasing into the band of interest. To ensure that these filters and the external resistors do not cause gain errors, the reference buffers are enabled. The analog input buffers are enabled automatically because these buffers are enabled when the PGA is used. The reference buffers require some headroom (100 mV within the power supply rails). Therefore, a 470 Ω resistor was included on the low side to allow this headroom.

The 250 μA excitation current requires 370 mV of headroom. The voltage seen on this pin is $(470 \Omega \times 2 \times 250 \mu\text{A}) + (5600 + 313.71) \Omega \times 250 \mu\text{A} = 1.713 \text{ V}$, which is acceptable.

The [Circuit Note CN-0383](#) provides further detail on interfacing 3-wire Pt100 sensors to the [AD7124-4](#) and linearizing or post-processing the conversions.

The circuit shown in Figure 1 also supports a 3-wire Pt1000 RTD. The circuit connections are the same as used for the Pt100. The ADC configuration used is as described previously in this section, but with the PGA gain set to 1.

Thermocouple

Figure 4 shows how a thermocouple connects to the circuit.

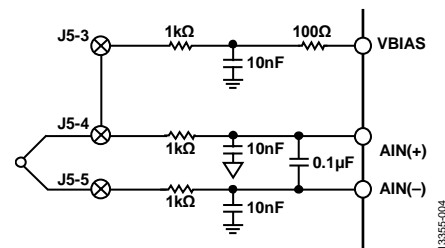


Figure 4. T-Type Thermocouple

A thermocouple consists of a connection of two different types of wire. A voltage is generated, which is dependent on temperature. For example, a T-type thermocouple generates a voltage of 40 μV typically when a 1°C change in temperature occurs.

The thermocouple voltage must be biased to a voltage. The [AD7124-4](#) contains a V_{BIAS} source that biases the thermocouple to $(AV_{DD} - AV_{SS})/2$. The bias voltage is enabled on the AIN6 channel and applied to the thermocouple, as shown in Figure 4. The bias voltage can also be enabled on the AINM pin of the analog input. However, the external R and C values must be limited in this case, because there is a difference between the bias voltage seen on AINM and the filtered version seen on AINP; this difference is sufficiently high that it affects the conversion result.

The thermocouple measurement is an absolute measurement, the internal 2.5 V reference being used for the conversion. A T-type thermocouple is used. This thermocouple can measure temperatures from -200°C to +400°C, leading to a voltage range of -8 mV to +16 mV being generated by the thermocouple. The PGA is set to 128.

For the cold junction compensation, an NTC thermistor is used (10 kΩ, 1%, 3435 K).

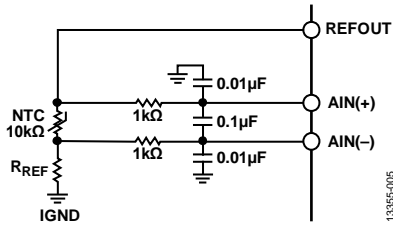


Figure 5. Thermistor

The internal reference supplies the thermistor, the gain being set to 1 for this conversion. A resistor, R_{REF} , is used on the low side of the thermistor. This is a precision 5.6 kΩ resistor (0.05%, 10 ppm/°C). The voltage across the thermistor V_{NTC} is

$$V_{NTC} = \frac{V_{REF} \times ADC_{CODE}}{2^{24}}$$

where:

V_{REF} is the reference voltage.

ADC_{CODE} is the code read from the AD7124-4.

2^{24} is the maximum code from ADC.

The resistance of the thermistor, R_{NTC} , is

$$R_{NTC} = \frac{V_{NTC} \times R_{REF}}{V_{REF} - V_{NTC}}$$

where:

$R_{REF} = 5.6 \text{ k}\Omega$.

V_{REF} is the reference voltage.

Combining these equations,

$$R_{NTC} = \frac{ADC_{CODE} \times R_{REF}}{FS_{CODE} - ADC_{CODE}}$$

where:

ADC_{CODE} is the code read from the AD7124-4.

$R_{REF} = 5.6 \text{ k}\Omega$.

FS_{CODE} is the full-scale code from the AD7124-4 (2^{24}).

The resistance is then converted to temperature in the microcontroller using a look-up table based on the thermistor equation:

$$T = \frac{1}{\frac{\ln\left(\frac{R_{NTC}}{R_0}\right)}{\beta} + \frac{1}{T_0}}$$

where:

T is the temperature recorded by thermistor (K).

$R_0 = 10 \text{ k}\Omega$.

$\beta = 3435 \text{ K}$.

$T_0 = 298.15 \text{ K}$.

The resulting temperature in °C is $T - 273.15$.

The 5.6 kΩ resistor also provides headroom for the analog input because the analog input buffers are enabled, and they require

100 mV of headroom. This resistor also protects the circuit because it limits the current if miswiring occurs.

The Circuit Note CN-0384 provides further detail on interfacing thermocouple sensors to the AD7124-4 and linearizing or post-processing the conversions.

Pressure Sensor

A voltage excited pressure sensor is connected as shown in Figure 6 while a current-excited pressure sensor is connected as shown in Figure 7. A Honeywell pressure sensor (Honeywell S&C 24PCDFA6D) is used.

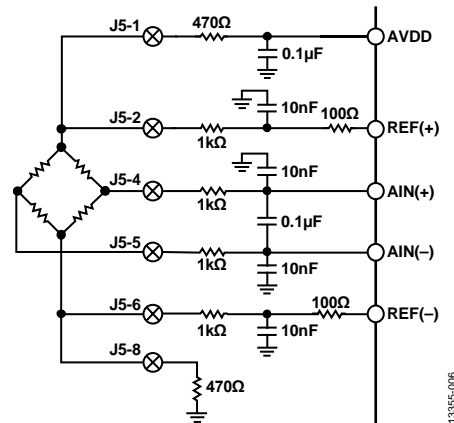


Figure 6. Voltage Excited Pressure Sensor

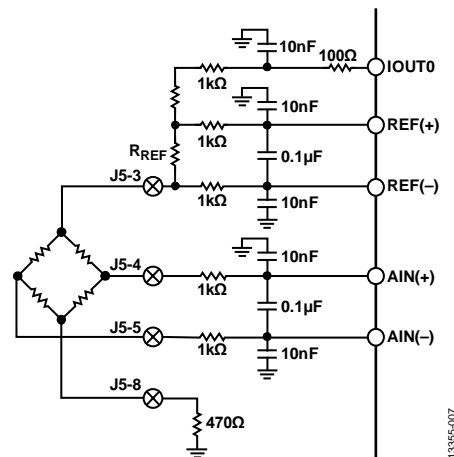


Figure 7. Current Excited Pressure Sensor

For the voltage excited architecture, AV_{DD} (3.3 V) excites the sensor. If AV_{DD} is used to excite the load cell, the excitation voltage can be used directly as the ADC reference. Note that a resistor was added on the high side and the low side of the sensor to ensure that the headroom requirements of the AD7124-4 buffers are met. A gain of 16 is used.

For the current excited mode, both of the 100 μA excitation currents of the AD7124-4 are directed to Pin AIN6, resulting in a 200 μA excitation current for the sensor. Again, the gain is set to 16. A 5.6 kΩ precision resistor generates the reference. This arrangement results in a ratiometric configuration, that is, any deviation in the excitation current value has no effect on the system accuracy.

The circuit board includes the option to connect the sensor low side to GND or to the power switch of the [AD7124-4](#).

As previously stated, the analog inputs and reference inputs have antialias filters to reject any interference that occur at multiples of the ADC sampling frequencies. The series resistors also limit the current if an overvoltage occurs.

Primary Sensor Simulation

The circuit includes a resistor network and potentiometer that allows sensor simulation (primary sensor simulation circuit shown in Figure 1). Using the potentiometer, the voltage applied between AIN0 (AINP) and AIN1 (AINM) can be varied from approximately -0.09 V to approximately $+1.36$ V. This circuit uses the internal reference for the conversions; the [AD7124-4](#) gain is set to 1, and the analog input buffers are enabled. This configuration allows the user to evaluate the circuit without needing to connect an external sensor.

Digital Data Processing, Algorithm, and Communications

The demonstration software (included in the [CN-0382 Design Support Package](#)) performs the initialization and configuration, processes data from the analog inputs, controls the analog output, and performs the HART communication. All the sensors mentioned require linearization or compensation. This linearization is performed in the software. See the [Circuit Note CN-0381](#), [Circuit Note CN-0383](#), and [Circuit Note CN-0384](#) for further details on the RTD and thermocouple sensors and the linearization required.

Analog Output

The [AD5421](#) integrates a low power, precision, 16-bit DAC with a 4 mA to 20 mA, loop powered output driver and provides all functions required for the field instrument analog output.

The [AD5421](#) interfaces with the microcontroller via the SPI interface.

The [AD5421](#) also includes a range of diagnostic functions related to the 4 mA to 20 mA loop. The auxiliary ADC can measure the voltage across the instruments loop terminals via the $20\text{ M}\Omega/1\text{ M}\Omega$ resistive divider connected to the V_{LOOP} pin. The ADC can also measure the chip temperature via the integrated sensor. The microcontroller can configure and read all the diagnostics of the [AD5421](#); however, the [AD5421](#) can also operate autonomously.

As an example, if the communication between the controller and the [AD5421](#) fails, the [AD5421](#) automatically sets its analog output to a 3.2 mA alarm current after a defined period. This alarm current indicates to the host that the field instrument failed to operate.

The software controls any change of the output current from one value to another to prevent disturbance of the HART communication.

HART Communication

The [AD5700](#) integrates a complete HART FSK modem. The modem connects to the microcontroller via a standard UART interface, complemented by request to send (RTS) and carrier detect (CD) signals.

The HART output is scaled to the required amplitude by the $0.068\text{ }\mu\text{F}/0.22\text{ }\mu\text{F}$ capacitive divider and coupled to the [AD5421](#) C_{IN} pin, where it is combined with the DAC output to drive and modulate the output current.

The HART input is coupled from LOOP+ via a simple passive RC filter to the [AD5700](#) ADC_IP pin. The RC filter operates as the first stage band-pass filter for the HART demodulator and also improves the system electromagnetic immunity, which is important for robust applications working in harsh industrial environments.

The [AD5700](#) low power oscillator generates the clock for the HART modem with a 3.6864 MHz external crystal connected directly to the XTAL1 and XTAL2 pins.

Output Protection

A transient voltage suppressor (TVS) protects the 4 mA to 20 mA HART interface from overvoltage. Select the TVS voltage rating so that the [AD5421](#) absolute maximum voltage of 60 V on the REG_{IN} pin is not exceeded. Note that the TVS leakage current can affect the current output accuracy; therefore, pay attention to the leakage current at a given loop voltage and temperature range when selecting this component.

An external depletion-mode FET can be used with the [AD5421](#) to increase the loop voltage maximum.

The circuit is protected against reversed polarity by a pair of diodes in series with loop output.

The ferrite beads in series with the loop together with the 4700 pF capacitor improve the system EMC performance. Do not use a higher capacitance across the loop terminals because of the HART network specifications.

The 4.7 V, low leakage, Zener diode protects the [AD5421](#) on-chip, 50 Ω loop sense resistor in the event of an accidental external voltage between the [AD5421](#) COM pin and LOOP- pin (for example, when debugging the circuit).

Power Supplies and Power Management

The complete field instrument circuitry, including the sensor drive current, must operate on the limited amount of power available from the 4 mA to 20 mA loop. This is a common challenge in any loop powered field instrument design. The circuit in Figure 1 provides an example of delivering both a low power and high performance solution. All integrated circuits used in the application are designed for low power, and the circuit leverages their integrated features to deliver a flexible power management structure and an optimum loop powered solution.

The [AD5421](#) is powered by the 4 mA to 20 mA loop voltage and provides a regulated low voltage for the rest of the circuit. The [AD5421](#) REG_{OUT} voltage is pin programmable from 1.8 V to 12 V depending on circuit requirements. The circuit in Figure 1 uses the 9 V supply voltage option. The sensor side is isolated from the 4-20 mA loop using a simple push-pull, dc-to-dc converter. The [ADG5433](#) is clocked from the microcontroller and generates 9 V non-overlapping square waves, which drive a transformer. The transformer works in voltage ratio 2:1. The 4.5 V on the secondary side is rectified and regulated by the [ADP162](#) to generate a low noise 3.3 V supply for the [AD7124-4](#). Both the analog and digital 3.3 V supplies of the [AD7124-4](#) are supplied by the [ADP162](#) regulator. However, a filter (L1/R19) is included to prevent noise from the digital circuitry being fed into the analog sections.

The [AD5421](#) supplies the 3.3 V logic supply on the loop side. This supply is used directly by the microcontroller and the [AD5700](#).

The REG_{OUT} RC filter (10 μ F/10 Ω /10 μ F) helps to prevent any interference coming from the loop affecting the analog circuitry. It also prevents any interference generated by the circuit, specifically by the controller and the digital circuitry, from coupling back to the loop, which is important for a reliable HART communication.

The [AD5700](#) HART modem is supplied through an additional RC filter (470 Ω /1 μ F). This filter is very important in the loop powered application because it prevents current noise from the [AD5700](#) from coupling to the 4 mA to 20 mA loop output, which would otherwise affect the HART communication. The [AD5700](#) modem uses the external crystal with 8.2 pF capacitors to ground on the XTAL1 and XTAL2 pins, which is the option using the least possible power.

One of the major advantages of the [AD7124-4](#) is that it gives the user the flexibility to employ one of three integrated power modes. The current consumption, range of output data rates, and rms noise can be tailored with the power mode selected. Therefore, for 4 mA to 20 mA or portable equipment, the low or mid power mode is the optimum choice. For process control systems where power consumption is not a concern, the full power mode can be used, which leads to lower noise. For this loop powered circuit, the mid power mode is used. See the [AD7124-4](#) data sheet for further information on the power modes.

The PSW ground switch pin of the [AD7124-4](#) controls the excitation/power supply when the pressure transducer is connected. The switch is off by default at the instrument power up. This default allows the system to be fully configured, including appropriate power modes, before turning on the sensor, and thus minimizes any possible power-up spikes on the 4 mA to 20 mA loop output.

When an RTD sensor is connected, it is supplied from the programmable current source of the [AD7124-4](#), and therefore, its power is fully controlled by the software. Similarly, for

thermocouple sensors, the bias voltage and absolute reference are embedded in the [AD7124-4](#) and therefore software controlled.

Software

The microcontroller interfaces to the [AD7124-4](#) and [AD5421](#) using SPI interfaces. It communicates with the [AD5700](#) via a UART interface, UART0. Software is downloaded to the microcontroller via the second UART interface on the microcontroller, UART1.

On start-up, the microcontroller configures all three devices, the [AD7124-4](#) being configured for a T-type thermocouple. The [AD7124-4](#) is operated in continuous conversion mode. Therefore, its $DOUT/\overline{RDY}$ pin is connected to an interrupt on the microcontroller also. Each time a conversion is available from the ADC, an interrupt to the microcontroller is generated and the conversion is read. The microcontroller then linearizes and processes the data. The result is sent to the [AD5421](#) DAC for transmission on the 4 mA to 20 mA loop. The software used to demonstrate the functionality and performance of the circuit is contained in the [CN-0382 Design Support Package](#). The software supports all the sensor types mentioned in this circuit note. Documentation on how to alter the software for the different sensor types and details on downloading the software to the microcontroller are also provided in the [CN-0382 Design Support Package](#).

The code example includes a basic HART slave command response to demonstrate the hardware function and capability. However, the code example does not include the protocol layers of the HART communication.

COMMON VARIATIONS

The [AD7124-4](#) has a high performance and very flexible analog front-end, with four differential or seven pseudo differential analog input pins and extra pins for voltage reference and low side power switch. It allows direct interface to multiple analog sensors of varying types, such as any resistive bridge sensors, resistive temperature sensors, or thermocouples. Therefore, do not limit the field instrument solution to the sensor types listed in this circuit note only, because it can be used for almost any sensor field instrument.

The [AD7124-8](#) can be used as an alternative to the [AD7124-4](#). Both the [AD7124-4](#) and [AD7124-8](#) have the same performance. However, the [AD7124-8](#) offers 8 differential or 15 pseudo differential inputs, and therefore is suitable for applications that require a high channel count.

The [AD5421](#) can be connected via the protection directly to the loop. Alternatively, a depletion mode N-channel MOSFET can be connected between the [AD5421](#) and the loop power supply, as shown in Figure 8. The use of the additional MOSFET in this configuration keeps the voltage drop across the [AD5421](#) at approximately 12 V, lowers the power dissipated in the [AD5421](#) package, and therefore improves the 4 mA to 20 mA analog output accuracy. It also increases the maximum voltage allowed

in the loop to the level of the MOSFET rating. The additional MOSFET has no effect on the HART communication.

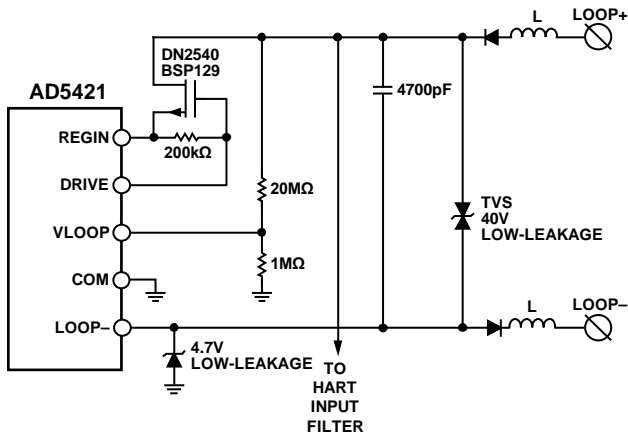


Figure 8. MOSFET Connected to the AD5421 Loop Power Supply

The AD5700 is used with a 3.6864 MHz crystal in this circuit, which is the configuration achieving the lowest power consumption. Alternatively, the AD5700-1, with an integrated 0.5% precision internal oscillator, can be used. The internal oscillator increases the modem power supply current by 225 μ A maximum, compared to the crystal oscillator; however, because no external crystal is needed, this option provides both cost savings and reduced board area requirements.

For applications that are not loop powered, the AD5410, AD5420, AD5422, or AD5755 are good choices for the 4 mA to 20 mA DAC.

Finally, there are a wide choice of isolator products that can be used instead of the ADuM1441: the ADuM1440, ADuM1442, ADuM1445, ADuM1446, ADuM1447, ADuM1240, ADuM1241, ADuM1245, and ADuM1246.

CIRCUIT EVALUATION AND TEST

Circuit Hardware

The circuit shown in Figure 1 is built on the DEMO-AD7124-DZ printed circuit board (PCB) shown in Figure 9.

The DEMO-AD7124-DZ circuit board includes additional features for easy system evaluation. The RTD, thermocouple, or pressure sensor can be connected via the 8-pin connector, J5. There are test points for HART RTS and CD. The 4-pin connector allows code to be downloaded to the microcontroller.

The CN-0382 Design Support Package also includes a full field instrument C-code example for 3-wire and 4-wire Pt100 and Pt1000 RTDs, thermocouples, and voltage/current excited pressure sensors, which enables complete verification and evaluation of all hardware blocks and features of the circuit, and a limited verification of the HART interface functionality. For detailed information about HART interface specifications and resources, contact the Hart Communication Foundation.

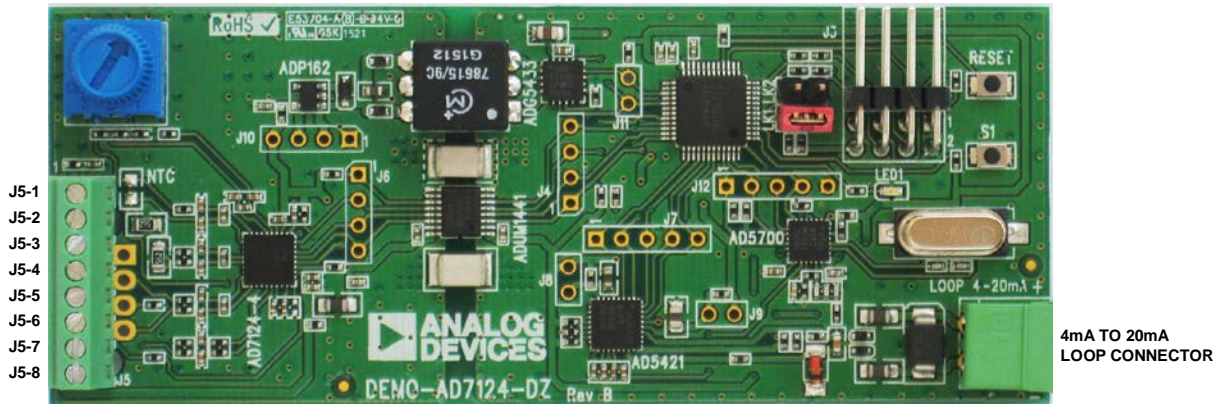


Figure 9. DEMO-AD7124-DZ Printed Circuit Board

Circuit Power Consumption

For ease of in-circuit measurement, the circuit has numerous test points to measure the current. The REG_{OUT} pin and DV_{DD} pins of the AD5421 include a 10 Ω resistor in their path. The output of the ADP162 has a similar 10 Ω resistor in its path. There are test points on each side of the 10 Ω resistors. This setup allows the voltage drop across each resistor to be measured, and the current to be calculated without interrupting the supply current or disturbing the circuit.

The circuit is configured as follows:

- Microcontroller core clock = 1 MHz
- AD7124-4 and the analog circuitry operating in the relevant mode per individual sensor type
- AD5421 operating and updating loop output current at a rate of 10 SPS
- HART communicating, periodically responding to master request to read all device variables

Table 1. Circuit Current Consumption

Mode	AD5421 Internal (mA)	DVDD 3.3 V (mA)	REGOUT 9.0 V (mA)	Total Off Loop (mA)	Isolated 3.3 V (mA)
Simulation	0.28	0.63	0.82	1.73	0.48
RTD 4-wire	0.28	0.63	1.00	1.91	0.84
RTD 3-wire	0.28	0.63	1.12	2.03	1.08
TC	0.28	0.63	0.89	1.80	0.61
Pressure					
V Mode	0.28	0.63	1.16	2.07	1.15
I Mode	0.28	0.63	0.98	1.89	0.79

Table 1 shows the power supply current for each of the individual blocks: the AD5421 itself (estimation, verified by placing the AD5421 into a minimum loop current), the circuitry supplied from DV_{DD} 3.3 V (the microcontroller, the HART modem, and the primary side of the SPI isolation), and the primary 9 V side of the isolated power supply. These components together sum into the total current taken off the loop for the circuit itself, before adding the variable current component to make the 4 mA to 20 mA output. The Isolated 3.3 V column is the current from the isolated 3.3 V, which supplies the sensor, the AD7124-4, and the secondary side of the SPI isolation.

The circuit with all relevant analog and digital blocks, including the input sensor, consumes a power supply current well within the budget allowed at the minimum 4 mA loop output current.

Sensor Input Performance

4-Wire RTD

Figure 10 shows the performance of the system when connected to a 4-wire RTD. A B Grade Pt100 sensor is used. The AD7124-4 configuration is as follows:

- Power mode: mid power mode
- Filter: post filter, 25 SPS
- Excitation current: enabled on AIN6 and set to 250 μA
- Gain = 16
- Polarity: unipolar
- Reference buffers enabled
- RTD connected to the AIN4/AIN5 channel
- Reference: REFIN1 with 5.6 kΩ reference resistor connected across the REFIN1 terminals
- AD7124-4 internal offset and full-scale calibration was performed on power-up

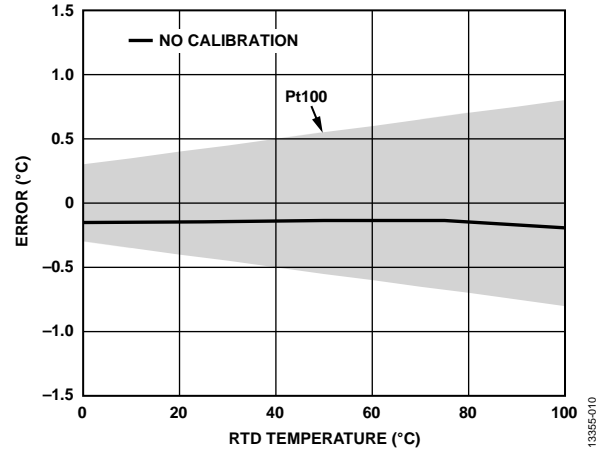


Figure 10. 4-Wire RTD Measurement

The conversions read from the ADC were linearized within the microcontroller. The temperature forced on the Pt100 sensor was swept from 0°C to 100°C while the circuit board was held at 25°C. Figure 10 shows the accuracy of the demonstration. The measured accuracy of the demonstration is within the specified accuracy of a B Grade Pt100 sensor.

3-Wire RTD

Figure 11 shows the performance of the system when connected to a 3-wire RTD. A B Grade Pt100 is used. The AD7124-4 configuration is as follows:

- Power mode: mid power mode
- Filter: post filter, 25 SPS
- Excitation Current IOUT0: enabled on AIN6 and set to 250 μ A
- Excitation Current IOUT1: enabled on AIN7 and set to 250 μ A
- Gain = 16
- Polarity: unipolar
- Reference buffers enabled
- RTD connected to the AIN4/AIN5 channel
- Reference: REFIN1 with 5.6 k Ω reference resistor connected across the REFIN1 terminals
- AD7124-4 internal offset and full-scale calibration performed on power-up

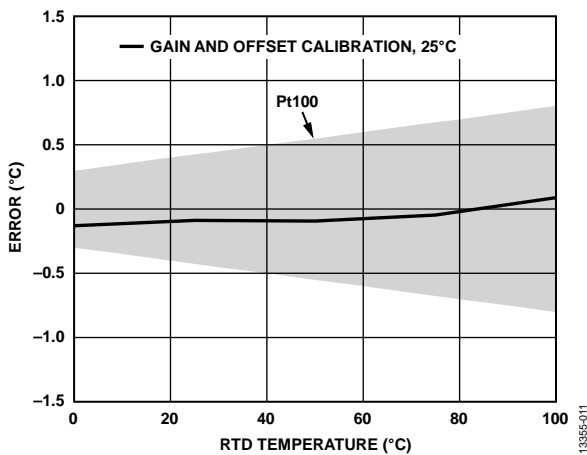


Figure 11. 3-Wire RTD Measurement

The temperature forced on the Pt100 sensor was swept from 0°C to 100°C while the circuit board was held at 25°C. The conversions read from the ADC were linearized within the microcontroller. The resulting error between the forced temperature and the temperature measured by the circuit board is shown. An internal offset and full-scale calibration were performed at 25°C prior to the temperature sweep. Following the calibration, the 3-wire Pt100 is well within the envelope allowed for a B Grade Pt100. Figure 11 shows the accuracy of the demonstration. The measured accuracy of the demonstration is within the specified accuracy of a B Grade Pt100 sensor.

Thermocouple

Figure 12 shows the performance of the system when connected to a T-type thermocouple. The AD7124-4 configuration is as follows:

- Power mode: mid-power mode
- Thermocouple configuration
 - Gain = 128
 - Channel: AIN4/AIN5
 - Internal reference enabled
 - Filter: post filter, 25 SPS
 - Polarity: bipolar
- AD7124-4 internal offset and full-scale calibration performed on power-up
- Cold junction configuration
 - Gain = 1
 - Filter: fast settling Sinc³, 44.44 SPS
 - Channel: AIN2/AIN3
 - Internal reference selected
 - Analog input buffers enabled
 - Polarity: unipolar

The full-scale error of the AD7124-4 is factory calibrated at a gain of 1; therefore, no additional calibrations were performed.

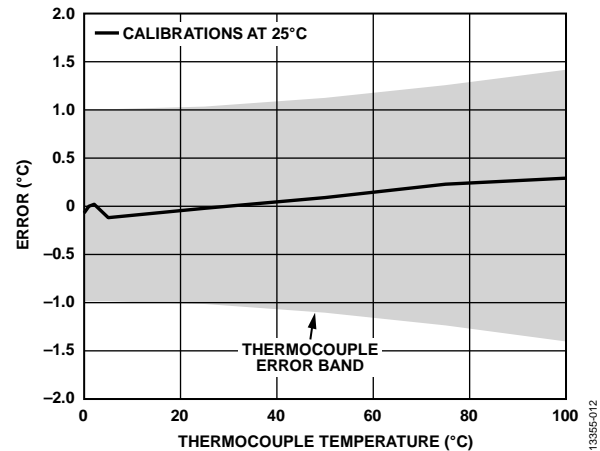


Figure 12. T-Type Thermocouple Measurement (Cold Junction at Ambient)

In Figure 12, the cold junction was held at 25°C, and the thermocouple was swept from 0°C to 100°C. The conversions read from the ADC were processed and linearized within the microcontroller.

A T-type thermocouple has an accuracy of 1°C or 0.75%, whichever is greater. The thermistor also adds some error. The thermistor used in the circuit has an accuracy of 1% or 1°C, whichever is greater. Figure 12 shows the difference between the forced temperature and the measured temperature. The results are well within specification for the thermocouple/thermistor combination.

The measurements were repeated with the thermocouple held at 25°C and the cold junction swept from 0°C to 80°C (see Figure 13). The system had an overall accuracy of 1.75°C, which can be improved by using a more accurate cold junction such as a Pt100 sensor.

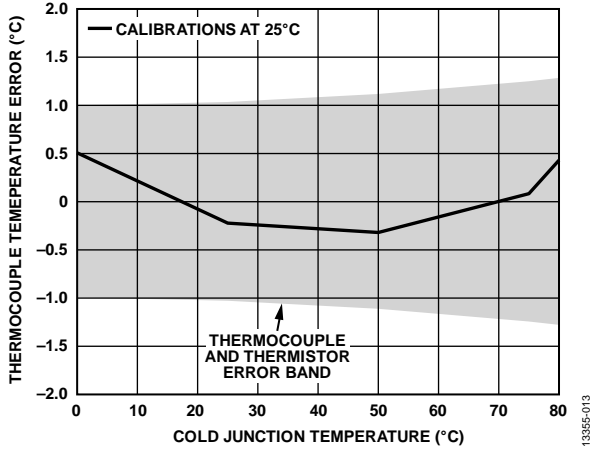


Figure 13. T-Type Thermocouple Measurement (Cold Junction Swept and Thermocouple Held at Ambient)

Pressure

With a pressure sensor connected, noise tests were performed. The level of noise is the main factor that can be influenced by the interaction of the analog front end with the rest of the circuitry on the board. Therefore, tests were performed to focus on the noise and related resolution performance of the system.

The demonstration was configured to transmit data, expressed as pressure in kPa, over the HART communication. One hundred samples were captured, and a basic data analysis to quantify the performance was completed. The first test was performed with a standard pressure sensor (Honeywell 24PCDFA6D) connected. A second test was performed with the input signal generated by a shorted input.

The testing was performed with the sensor being excited with a current source and with a voltage. In voltage mode, the AD7124-4 configuration is as follows:

- Power mode: mid power mode
- Filter: post filter, 25 SPS
- Gain = 16
- Polarity: bipolar
- Reference buffers enabled
- Sensor connected to the AIN4/AIN5 channel
- Reference: REFIN2, the reference being provided by the sense resistors of the pressure sensor.

In current excitation mode, the AD7124-4 configuration is as follows:

- Power mode: mid power mode
- Filter: post filter, 25 SPS
- Excitation current: both excitation currents enabled on AIN6 and set to 100 μA, resulting in a total current of 200 μA
- Gain = 16
- Polarity: bipolar
- Reference buffers enabled
- Sensor connected to the AIN4/AIN5 channel
- Reference: REFIN1 with 5.6 kΩ reference resistor connected across the REFIN1 terminals.

The performance summary is shown in Table 2, and the signal plots are shown in Figure 14 to Figure 17.

Table 2. Pressure Sensor: Noise and Resolution

Parameter	Voltage Mode		Current Mode		Unit
	Pressure Sensor	Shorted Input	Pressure Sensor	Shorted Input	
Full Scale	391.47	391.47	438.45	438.45	kPa
Noise RMS	0.66	0.61	1.76	1.69	Pa
Peak-to-Peak Noise	3.5	3.2	11.1	9.8	Pa
Effective (RMS) Resolution	19.2	19.3	17.9	18	Bits
Noise-Free (Peak-to-Peak) Resolution	16.8	16.9	15.3	15.4	Bits

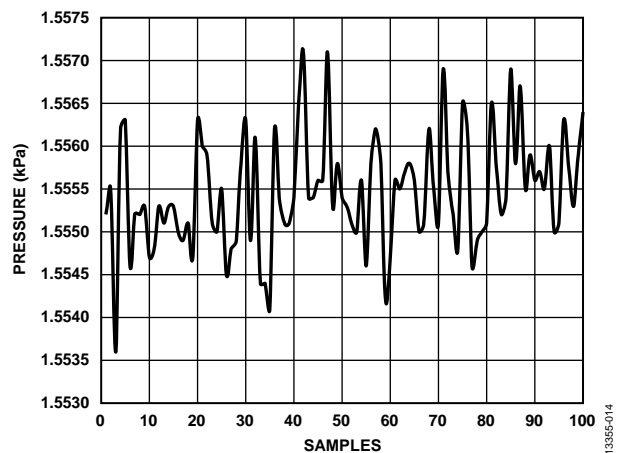


Figure 14. Voltage Mode—Pressure Sensor Input Waveform

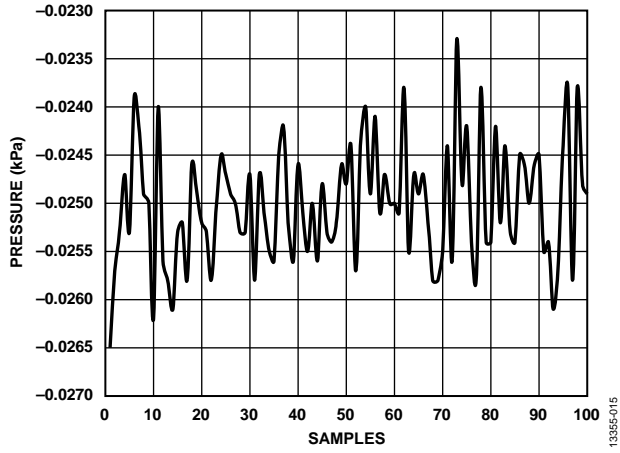


Figure 15. Voltage Mode—Shorted Input Waveform

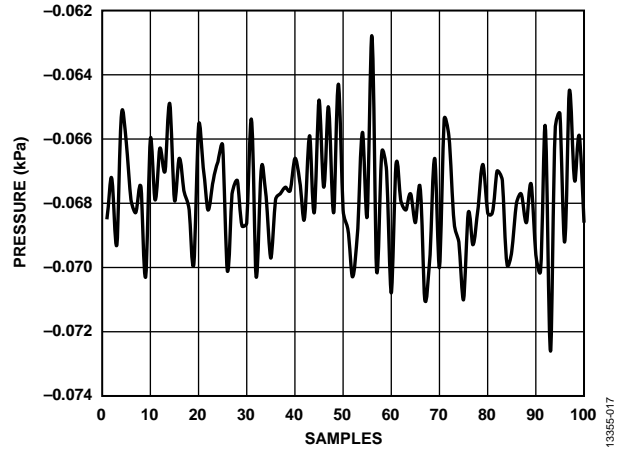


Figure 17. Current Mode—Shorted Input Waveform

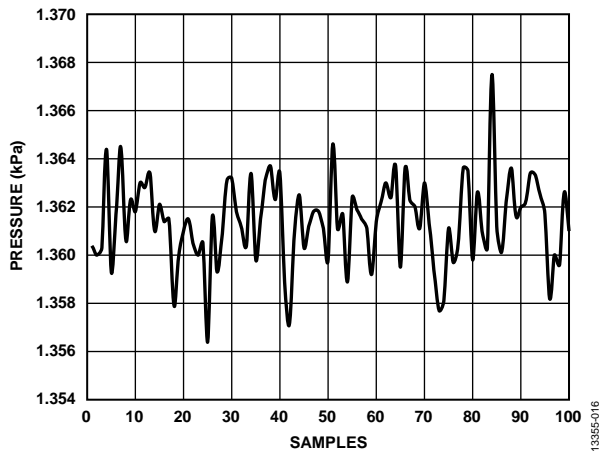


Figure 16. Current Mode—Pressure Sensor Input Waveform

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CN-0382 Design Support Package:

www.analog.com/CN0382-DesignSupport

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Circuit Note CN-0381. *Completely Integrated 4-Wire RTD Measurement System Using a Low Power, Precision, 24-Bit, Sigma-Delta ADC*. Analog Devices.

Circuit Note CN-0383. *Completely Integrated 3-Wire RTD Measurement System Using a Low Power, Precision, 24-Bit, Sigma-Delta ADC*. Analog Devices.

Circuit Note CN-0384. *Completely Integrated Thermocouple Measurement System Using a Low Power, Precision, 24-Bit, Sigma-Delta ADC*. Analog Devices.

HART® Communication Foundation

Data Sheets and Evaluation Boards

AD7124-4 Data Sheet and Evaluation Board

AD5421 Data Sheet and Evaluation Board

AD5700 Data Sheet and Evaluation Board

ADG5433 Data Sheet

ADuM1441 Data Sheet

ADP162 Data Sheet

REVISION HISTORY

10/2016—Rev. 0 to Rev. A

Changes to Common Variations Section.....7

7/2015—Revision 0: Initial Version

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