19-1230; Rev 2a; 6/97

EVALUATION KIT AVAILABLE

1GHz, Low-Power, SOT23, Current-Feedback Amplifiers with Shutdown

MAX4223–MAX4228

General Description

The MAX4223–MAX4228 current-feedback amplifiers combine ultra-high-speed performance, low distortion, and excellent video specifications with low-power operation. The MAX4223/MAX4224/MAX4226/MAX4228 have a shutdown feature that reduces power-supply current to 350µA and places the outputs into a high-impedance state. These devices operate with dual supplies ranging from ±2.85V to ±5.5V and provide a typical output drive current of 80mA. The MAX4223/MAX4225/MAX4226 are optimized for a closed-loop gain of +1 (0dB) or more and have a -3dB bandwidth of 1GHz, while the MAX4224/MAX4227/MAX4228 are compensated for a closed-loop gain of +2 (6dB) or more, and have a -3dB bandwidth of 600MHz (1.2GHz gain-bandwidth product).

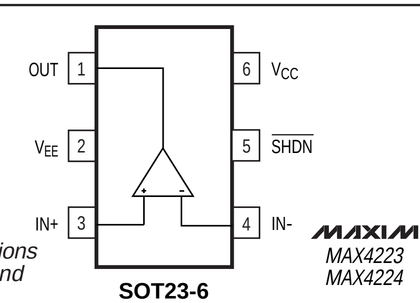
The MAX4223–MAX4228 are ideal for professional video applications, with differential gain and phase errors of 0.01% and 0.02°, 0.1dB gain flatness of 300MHz, and a 1100V/µs slew rate. Total harmonic distortion (THD) of -60dBc (10MHz) and an 8ns settling time to 0.1% suit these devices for driving high-speed analog-to-digital inputs or for data-communications applications. The low-power shutdown mode on the MAX4223/MAX4224/MAX4226/MAX4228 makes them suitable for portable and battery-powered applications. Their high output impedance in shutdown mode is excellent for multiplexing applications.

The single MAX4223/MAX4224 are available in space-saving 6-pin SOT23 packages. All devices are available in the extended -40°C to +85°C temperature range.

Applications

ADC Input Buffers	Data Communications
Video Cameras	Video Line Drivers
Video Switches	Video Multiplexing
Video Editors	XDSL Drivers
RF Receivers	Differential Line Drivers

Pin Configurations



SOT23-6

Pin Configurations continued at end of data sheet.

Features

- **Ultra-High Speed and Fast Settling Time:**
  - **1GHz -3dB Bandwidth (MAX4223, Gain = +1)**
  - **600MHz -3dB Bandwidth (MAX4224, Gain = +2)**
  - **1700V/µs Slew Rate (MAX4224)**
  - **5ns Settling Time to 0.1% (MAX4224)**
- **Excellent Video Specifications (MAX4223):**
  - **Gain Flatness of 0.1dB to 300MHz**
  - **0.01%/0.02° DG/DP Errors**
- **Low Distortion:**
  - **-60dBc THD (f_C = 10MHz)**
  - **42dBm Third-Order Intercept (f = 30MHz)**
- **6.0mA Quiescent Supply Current (per amplifier)**
- **Shutdown Mode:**
  - **350µA Supply Current (per amplifier)**
  - **100kΩ Output Impedance**
- **High Output Drive Capability:**
  - **80mA Output Current**
  - **Drives up to 4 Back-Terminated 75Ω Loads to ±2.5V while Maintaining Excellent Differential Gain/Phase Characteristics**
- **Available in Tiny 6-Pin SOT23 and 10-Pin µMAX Packages**

Ordering Information

PART	TEMP. RANGE	PIN-PACKAGE	SOT TOP MARK
MAX4223EUT-T	-40°C to +85°C	6 SOT23	AAAD
MAX4223ESA	-40°C to +85°C	8 SO	—

Ordering Information continued at end of data sheet.

Selector Guide

PART	MIN. GAIN	AMPS PER PKG.	SHUT-DOWN MODE	PIN-PACKAGE
MAX4223	1	1	Yes	6 SOT23, 8 SO
MAX4224	2	1	Yes	6 SOT23, 8 SO
MAX4225	1	2	No	8 SO
MAX4226	1	2	Yes	10 µMAX, 14 SO
MAX4227	2	2	No	8 SO
MAX4228	2	2	Yes	10 µMAX, 14 SO

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For small orders, phone 408-737-7600 ext. 3468.

ABSOLUTE MAXIMUM RATINGS

Supply Voltage (V_{CC} to V_{EE})..12V
Analog Input Voltage ....(V_{EE} - 0.3V) to (V_{CC} + 0.3V)
Analog Input Current ....±25mA
$\overline{SHDN}$ Input Voltage.........................(V_{EE} - 0.3V) to (V_{CC} + 0.3V)
Short-Circuit Duration
OUT to GND..Continuous
OUT to V_{CC} or V_{EE}...5sec

Continuous Power Dissipation (T_A = +70°C)
6-Pin SOT23 (derate 7.1mW/°C above +70°C).............571mW
8-Pin SO (derate 5.9mW/°C above +70°C)...................471mW
10-Pin µMAX (derate 5.6mW/°C above +70°C) 444mW
14-Pin SO (derate 8.3mW/°C above +70°C)................667mW
Operating Temperature Range ....-40°C to +85°C
Storage Temperature Range ....-65°C to +150°C
Lead Temperature (soldering, 10sec) ....+300°C

Stresses beyond those listed under "Absolute Maximum Ratings" may cause permanent damage to the device. These are stress ratings only, and functional operation of the device at these or any other conditions beyond those indicated in the operational sections of the specifications is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.

DC ELECTRICAL CHARACTERISTICS

(V_{CC} = +5V, V_{EE} = -5V, $\overline{SHDN}$ = 5V, V_{CM} = 0V, R_L = ∞ T_A = T_{MIN} to T_{MAX}, unless otherwise noted. Typical values are at T_A = +25°C.) (Note 1)

PARAMETER	SYMBOL	CONDITIONS		MIN	TYP	MAX	UNITS
Input Offset Voltage	V_{OS}	T_A = +25°C	MAX4223/MAX4224		±0.5	±4	mV
			MAX4225–MAX4228		±0.5	±5	
		T_A = T_{MIN} to T_{MAX}	MAX4223/MAX4224			±6	
			MAX4225–MAX4228			±7	
Input Offset Voltage Drift	TCV_{OS}				±2		µV/°C
Input Bias Current (Positive Input)	I_{B+}	T_A = +25°C			±2	±10	µA
		T_A = T_{MIN} to T_{MAX}				±15	
Input Bias Current (Negative Input)	I_{B-}	T_A = +25°C	MAX4223/MAX4224		±4	±20	µA
			MAX4225–MAX4228		±4	±25	
		T_A = T_{MIN} to T_{MAX}	MAX4223/MAX4224			±30	
			MAX4225–MAX4228			±35	
Input Resistance (Positive Input)	R_{IN+}				700		kΩ
Input Resistance (Negative Input)	R_{IN-}				45		Ω
Input Common-Mode Voltage Range	V_{CM}	Inferred from CMRR test		±2.5	±3.2		V
Common-Mode Rejection Ratio	CMRR	V_{CM} = ±2.5V	T_A = +25°C	55	61		dB
			T_A = T_{MIN} to T_{MAX}	50			
Operating Supply Voltage Range	V_{CC}/V_{EE}	Inferred from PSRR test		±2.85		±5.5	V
Power-Supply Rejection Ratio	PSRR	V_{CC} = 2.85V to 5.5V, V_{EE} = -2.85V to -5.5V	T_A = +25°C	68	74		dB
			T_A = T_{MIN} to T_{MAX}	63			
Quiescent Supply Current (per Amplifier)	I_{SY}	Normal mode ($\overline{SHDN}$ = 5V)			6.0	9.0	mA
		Shutdown mode ($\overline{SHDN}$ = 0V)			0.35	0.55	
Open-Loop Transresistance	T_R	V_{OUT} = ±2.5V	R_L = ∞	0.7	1.5		MΩ
			R_L = 50Ω	0.3	0.8		
Output Voltage Swing	V_{OUT}	R_L = 50Ω		±2.5	±2.8		V
Output Current (Note 2)	I_{OUT}	V_{OUT} = ±2.5V		60	80		mA
Short-Circuit Output Current	I_{SC}	R_L = short to ground			140		mA
$\overline{SHDN}$ Logic Low	V_{IL}					0.8	V
$\overline{SHDN}$ Logic High	V_{IH}			2.0			V

DC ELECTRICAL CHARACTERISTICS (continued)

(V_{CC} = +5V, V_{EE} = -5V, $\overline{SHDN}$ = 5V, V_{CM} = 0V, R_L = ∞, T_A = T_{MIN} to T_{MAX}, unless otherwise noted. Typical values are at T_A = +25°C.) (Note 1)

PARAMETER	SYMBOL	CONDITIONS	MIN	TYP	MAX	UNITS
$\overline{SHDN}$ Input Current	I_{IL}/I_{IH}	$\overline{SHDN}$ = 0V or 5V		25	70	µA
Shutdown Mode Output Impedance		$\overline{SHDN}$ = 0V, V_{OUT} = -2.5V to +2.5V (Note 3)	10	100		kΩ

AC ELECTRICAL CHARACTERISTICS

(V_{CC} = +5V, V_{EE} = -5V, $\overline{SHDN}$ = 5V, V_{CM} = 0V, A_V = +1V/V for MAX4223/MAX4225/MAX4226, A_V = +2V/V for MAX4224/MAX4227/MAX4228, R_L = 100Ω, T_A = +25°C, unless otherwise noted.) (Note 4)

PARAMETER	SYMBOL	CONDITIONS			MIN	TYP	MAX	UNITS
-3dB Small-Signal Bandwidth (Note 5)	BW	V_{OUT} = 20mVp-p		MAX4223/5/6	750	1000		MHz
				MAX4224/7/8	325	600		
Bandwidth for ±0.1dB Gain Flatness (Note 5)	$BW_{0.1dB}$	V_{OUT} = 20mVp-p		MAX4223/5/6	100	300		MHz
				MAX4224/7/8	60	200		
Gain Peaking		MAX4223/5/6				1.5		dB
		MAX4224/7/8				0.1		
Large-Signal Bandwidth	BW_{LS}	V_{OUT} = 2Vp-p		MAX4223/5/6		250		MHz
				MAX4224/7/8		330		
Slew Rate (Note 5)	SR	V_{OUT} = 4V step	Rising edge	MAX4223/5/6	850	1100		V/µs
				MAX4224/7/8	1400	1700		
			Falling edge	MAX4223/5/6	625	800		
				MAX4224/7/8	1100	1400		
Settling Time to 0.1%	t_S	V_{OUT} = 2V step		MAX4223/5/6		8		ns
				MAX4224/7/8		5		
Rise and Fall Time	t_r, t_f	V_{OUT} = 2V step		MAX4223/5/6		1.5		ns
				MAX4224/7/8		1.0		
Off Isolation		$\overline{SHDN}$ = 0V, f = 10MHz, MAX4223/4/6/8				65		dB
Crosstalk	X_{TALK}	f = 30MHz, R_S = 50Ω		MAX4225/6		-68		dB
				MAX4227/8		-72		
Turn-On Time from Shutdown	t_{ON}	MAX4223/4/6/8				2		µs
Turn-Off Time to Shutdown	t_{OFF}	MAX4223/4/6/8				300		ns
Power-Up Time	t_{UP}	V_{CC}, V_{EE} = 0V to ±5V step				100		ns
Differential Gain Error	DG	R_L = 150Ω (Note 6)		MAX4223/5/6		0.01		%
				MAX4224/7/8		0.02		
Differential Phase Error	DP	R_L = 150Ω (Note 6)		MAX4223/5/6		0.02		degrees
				MAX4224/7/8		0.01		
Total Harmonic Distortion	THD	V_{OUT} = 2Vp-p, f_C = 10MHz	R_L = 100Ω	MAX4223/5/6		-60		dBc
				MAX4224/7/8		-61		
			R_L = 1kΩ	MAX4223/5/6		-65		
				MAX4224/7/8		-78		

AC ELECTRICAL CHARACTERISTICS (continued)

(V_{CC} = +5V, V_{EE} = -5V, $\overline{SHDN}$ = 5V, V_{CM} = 0V, A_V = +1V/V for MAX4223/MAX4225/MAX4226, A_V = +2V/V for MAX4224/MAX4227/MAX4228, R_L = 100Ω, T_A = +25°C, unless otherwise noted.) (Note 4)

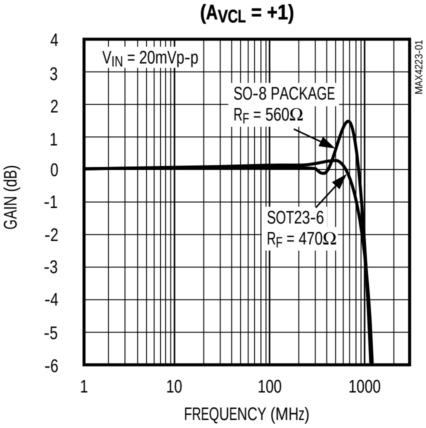
PARAMETER	SYMBOL	CONDITIONS		MIN	TYP	MAX	UNITS
Output Impedance	Z_{OUT}	f = 10kHz			2		Ω
Third-Order Intercept	IP3	f = 30kHz, f_Z = 30.1MHz	MAX4223/5/6		42		dBm
			MAX4224/7/8		36		
Spurious-Free Dynamic Range	SFDR	f = 10kHz	MAX4223/5/6		-61		dB
			MAX4224/7/8		-62		
1dB Gain Compression		f = 10kHz			20		dBm
Input Noise Voltage Density	e_n	f = 10kHz			2		nV/√Hz
Input Noise Current Density	i_n+, i_n-	f = 10kHz	IN+		3		pA/√Hz
			IN-		20		
Input Capacitance (Note 7)	C_{IN}	SO-8, SO-14 packages	Pin to pin		0.3		pF
			Pin to GND		1.0		
		SOT23-6, 10-pin µMAX packages	Pin to pin		0.3		
			Pin to GND		0.8		

Note 1: The MAX422_EUT is 100% production tested at T_A = +25°C. Specifications over temperature limits are guaranteed by design.
Note 2: Absolute Maximum Power Dissipation must be observed.
Note 3: Does not include impedance of external feedback resistor network.
Note 4: AC specifications shown are with optimal values of R_F and R_G. These values vary for product and package type, and are tabulated in the *Applications Information* section of this data sheet.
Note 5: The AC specifications shown are not measured in a production test environment. The minimum AC specifications given are based on the combination of worst-case design simulations along with a sample characterization of units. These minimum specifications are for design guidance only and are not intended to guarantee AC performance (see *AC Testing/Performance*). For 100% testing of these parameters, contact the factory.
Note 6: Input Test Signal: 3.58MHz sine wave of amplitude 40IRE superimposed on a linear ramp (0IRE to 100IRE). IRE is a unit of video signal amplitude developed by the International Radio Engineers. 140IRE = 1V.
Note 7: Assumes printed circuit board layout similar to that of Maxim's evaluation kit.

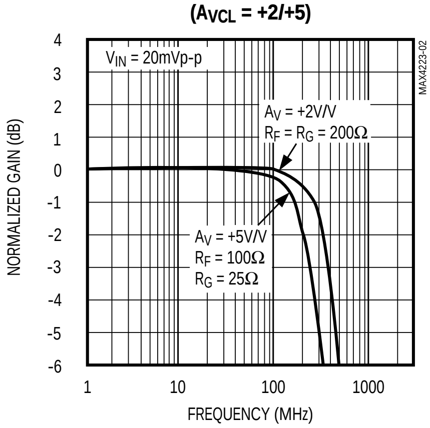
Typical Operating Characteristics

(V_{CC} = +5V, V_{EE} = -5V, R_L = 100Ω, T_A = +25°C, unless otherwise noted.)

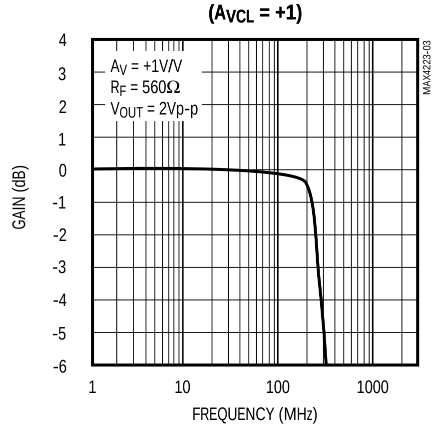
MAX4223 SMALL-SIGNAL GAIN vs. FREQUENCY (A_{VCL} = +1)



MAX4223 SMALL-SIGNAL GAIN vs. FREQUENCY (A_{VCL} = +2/+5)



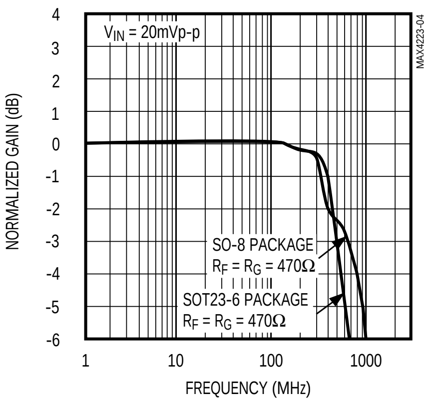
MAX4223/MAX4225/MAX4226 LARGE-SIGNAL GAIN vs. FREQUENCY (A_{VCL} = +1)



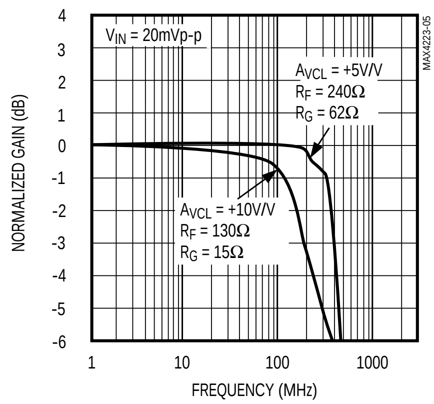
Typical Operating Characteristics (continued)

(V_{CC} = +5V, V_{EE} = -5V, R_L = 100Ω, T_A = +25°C, unless otherwise noted.)

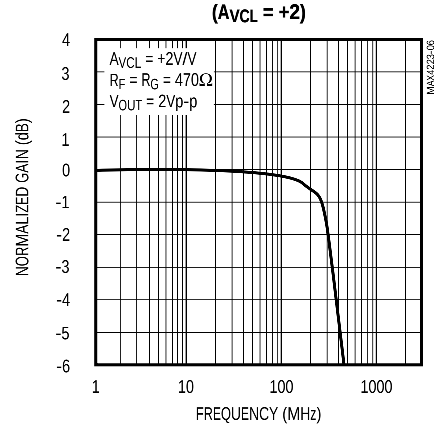
MAX4224
SMALL-SIGNAL GAIN vs. FREQUENCY
(A_{VCL} = +2)



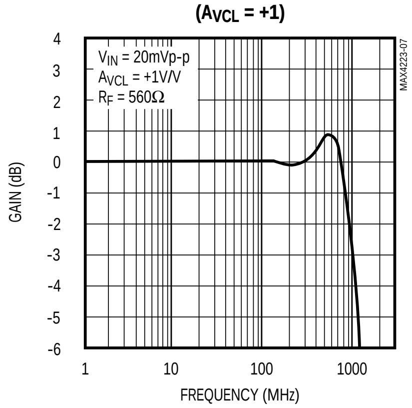
MAX4224
SMALL-SIGNAL GAIN vs. FREQUENCY
(A_{VCL} = +5/+10)



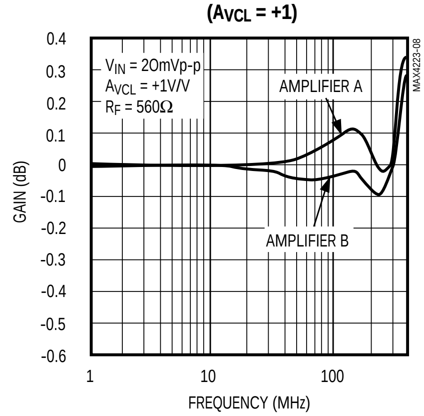
MAX4224/MAX4227/MAX4228
LARGE-SIGNAL GAIN vs. FREQUENCY
(A_{VCL} = +2)



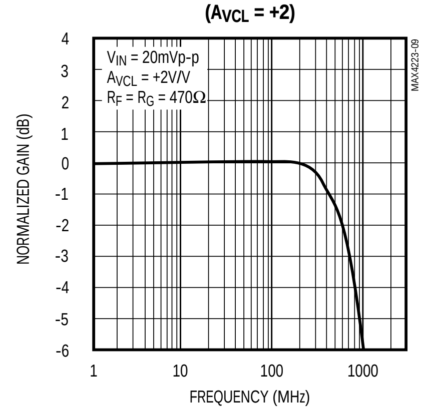
MAX4225/MAX4226
SMALL-SIGNAL GAIN vs. FREQUENCY
(A_{VCL} = +1)



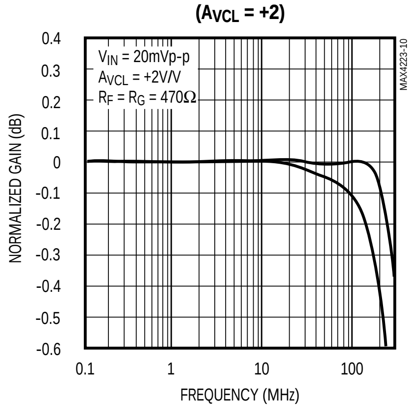
MAX4225/MAX4226
GAIN MATCHING vs. FREQUENCY
(A_{VCL} = +1)



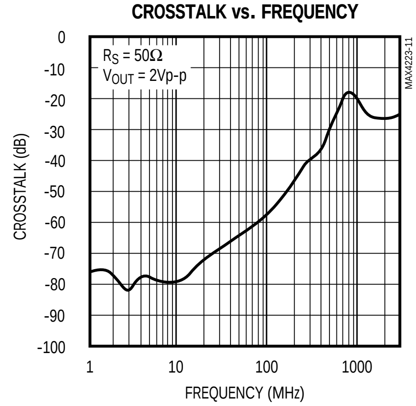
MAX4227/MAX4228
SMALL-SIGNAL GAIN vs. FREQUENCY
(A_{VCL} = +2)



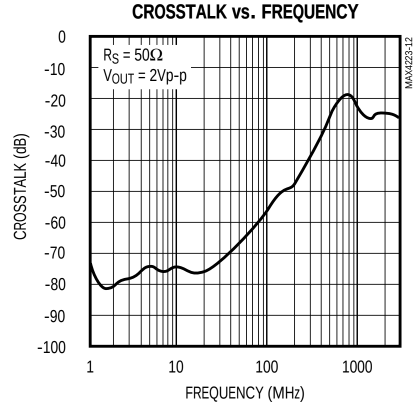
MAX4227/MAX4228
GAIN MATCHING vs. FREQUENCY
(A_{VCL} = +2)



MAX4225/MAX4226
CROSSTALK vs. FREQUENCY



MAX4227/MAX4228
CROSSTALK vs. FREQUENCY

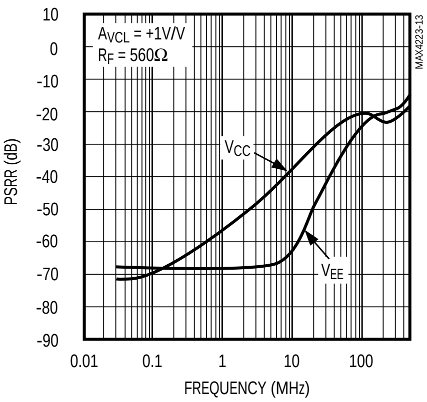


1GHz, Low-Power, SOT23, Current-Feedback Amplifiers with Shutdown

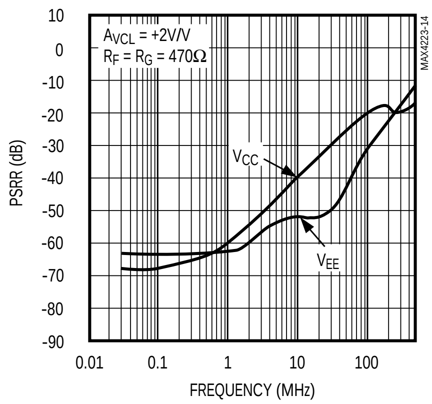
Typical Operating Characteristics (continued)

(V_{CC} = +5V, V_{EE} = -5V, R_L = 100Ω, T_A = +25°C, unless otherwise noted.)

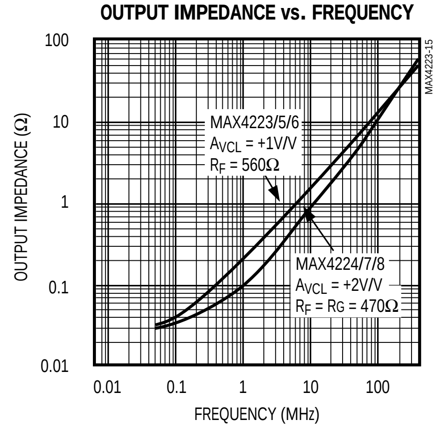
MAX4223/MAX4225/MAX4226 POWER-SUPPLY REJECTION RATIO vs. FREQUENCY (A_{VCL} = +1)



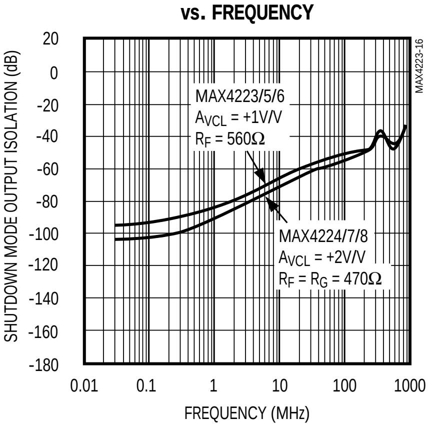
MAX4224/MAX4227/MAX4228 POWER-SUPPLY REJECTION RATIO vs. FREQUENCY (A_{VCL} = +2)



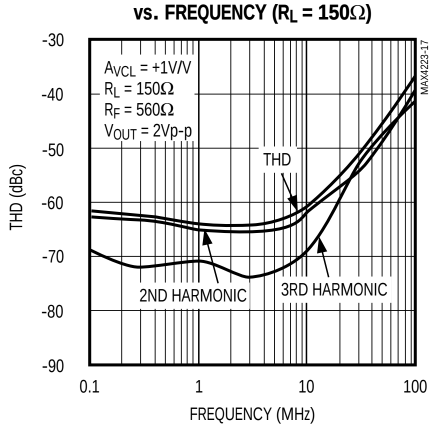
OUTPUT IMPEDANCE vs. FREQUENCY



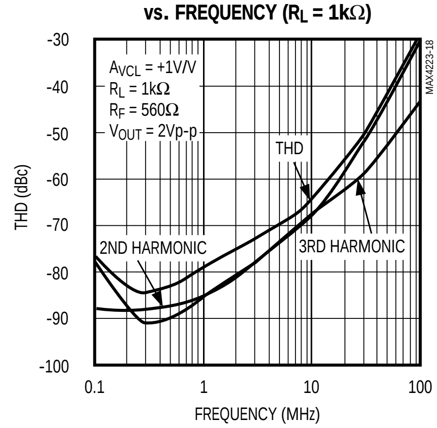
SHUTDOWN MODE OUTPUT ISOLATION vs. FREQUENCY



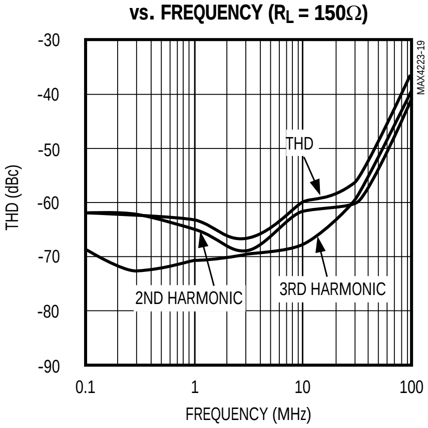
MAX4223/MAX4225/MAX4226 TOTAL HARMONIC DISTORTION vs. FREQUENCY (R_L = 150Ω)



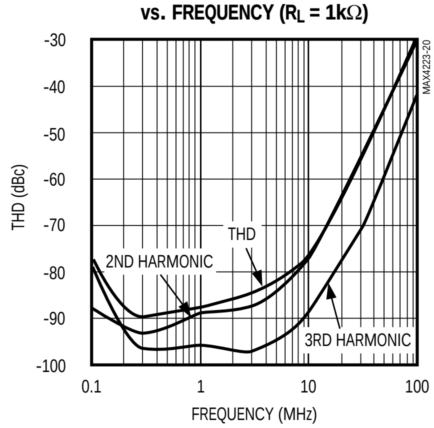
MAX4223/MAX4225/MAX4226 TOTAL HARMONIC DISTORTION vs. FREQUENCY (R_L = 1kΩ)



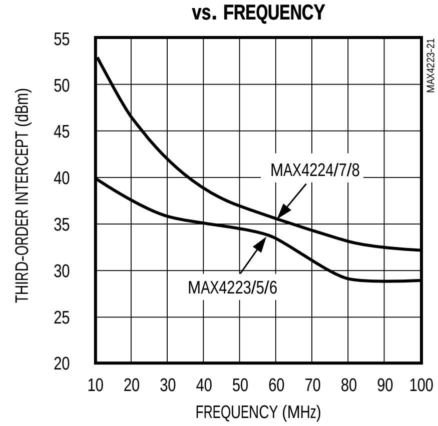
MAX4224/MAX4227/MAX4228 TOTAL HARMONIC DISTORTION vs. FREQUENCY (R_L = 150Ω)



MAX4224/MAX4227/MAX4228 TOTAL HARMONIC DISTORTION vs. FREQUENCY (R_L = 1kΩ)



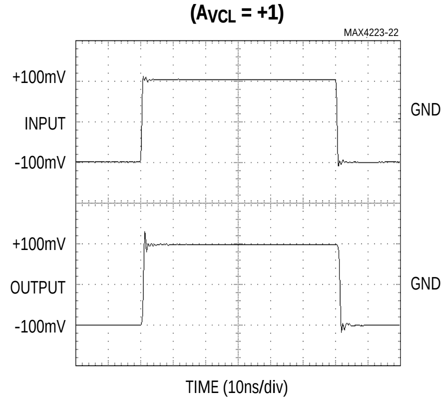
TWO-TONE THIRD-ORDER INTERCEPT vs. FREQUENCY



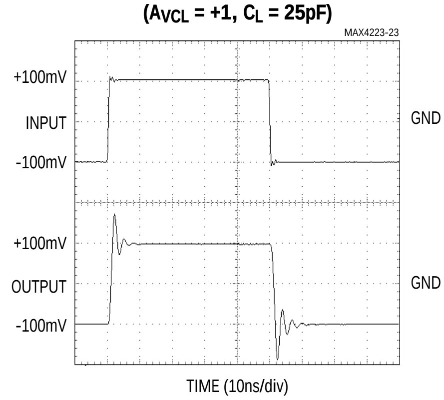
Typical Operating Characteristics (continued)

(V_{CC} = +5V, V_{EE} = -5V, R_L = 100Ω, T_A = +25°C, unless otherwise noted.)

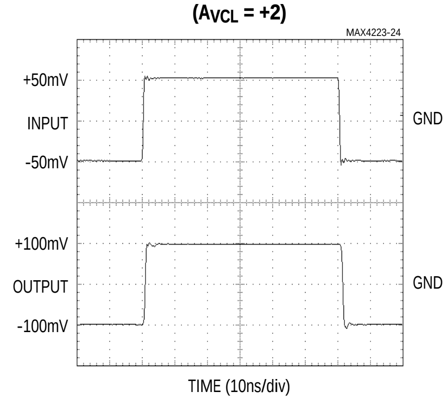
MAX4223/MAX4225/MAX4226 SMALL-SIGNAL PULSE RESPONSE (A_{VCL} = +1)



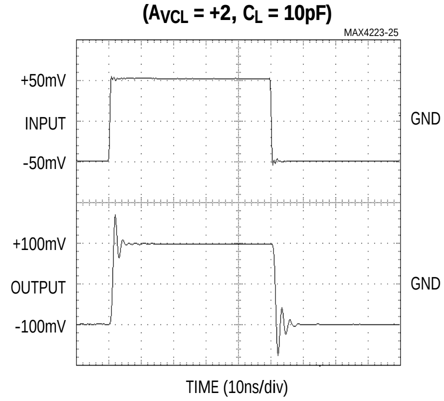
MAX4223/MAX4225/MAX4226 SMALL-SIGNAL PULSE RESPONSE (A_{VCL} = +1, C_L = 25pF)



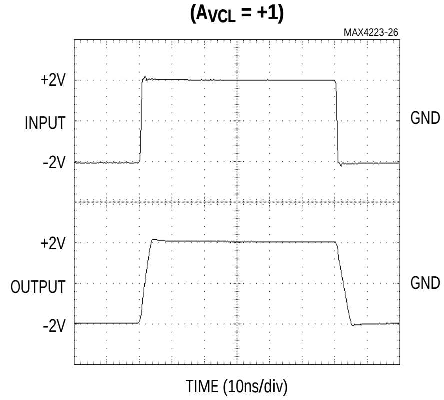
MAX4224/MAX4227/MAX4228 SMALL-SIGNAL PULSE RESPONSE (A_{VCL} = +2)



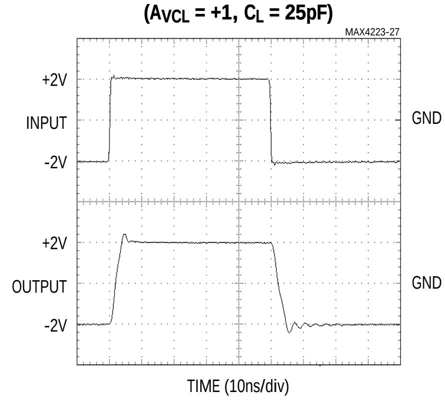
MAX4224/MAX4227/MAX4228 SMALL-SIGNAL PULSE RESPONSE (A_{VCL} = +2, C_L = 10pF)



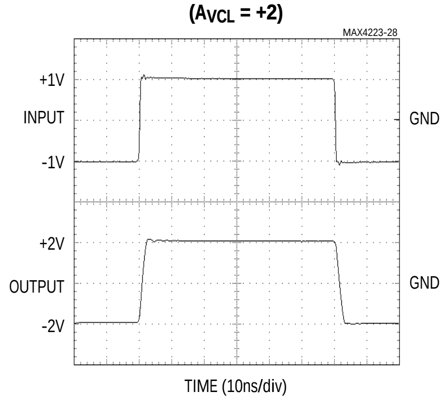
MAX4223/MAX4225/MAX4226 LARGE-SIGNAL PULSE RESPONSE (A_{VCL} = +1)



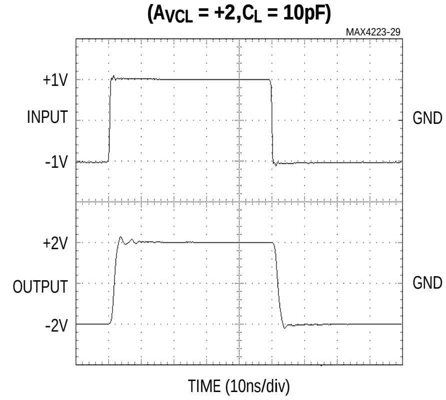
MAX4223/MAX4225/MAX4226 LARGE-SIGNAL PULSE RESPONSE (A_{VCL} = +1, C_L = 25pF)



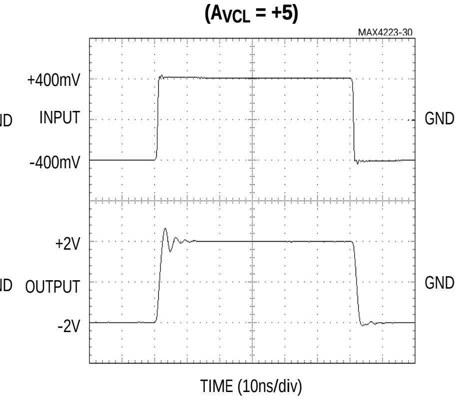
MAX4224/MAX4227/MAX4228 LARGE-SIGNAL PULSE RESPONSE (A_{VCL} = +2)



MAX4224/MAX4227/MAX4228 LARGE-SIGNAL PULSE RESPONSE (A_{VCL} = +2, C_L = 10pF)



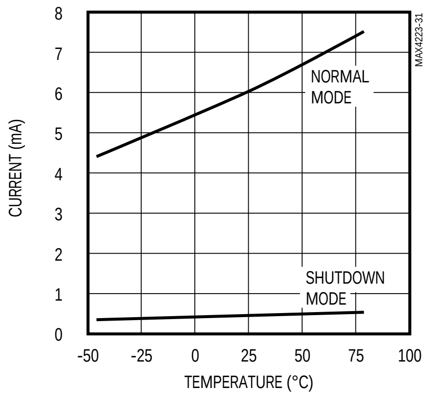
MAX4224/MAX4227/MAX4228 LARGE-SIGNAL PULSE RESPONSE (A_{VCL} = +5)



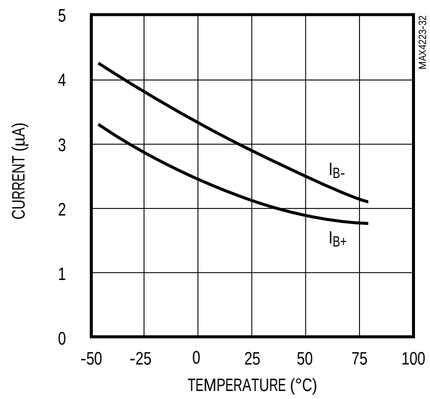
Typical Operating Characteristics (continued)

(V_{CC} = +5V, V_{EE} = -5V, R_L = 100Ω, T_A = +25°C, unless otherwise noted.)

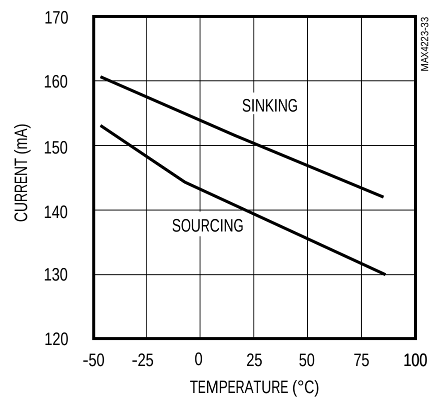
POWER-SUPPLY CURRENT PER AMPLIFIER vs. TEMPERATURE



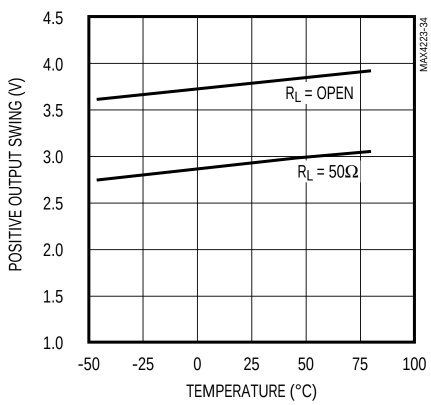
INPUT BIAS CURRENT vs. TEMPERATURE



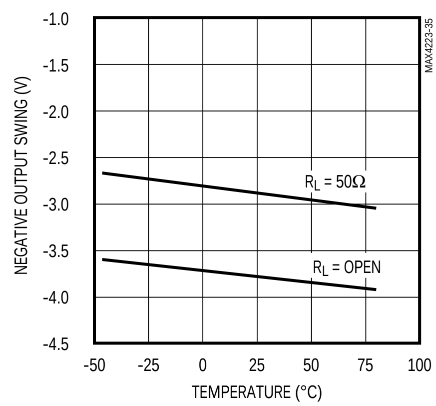
SHORT-CIRCUIT OUTPUT CURRENT vs. TEMPERATURE



POSITIVE OUTPUT SWING vs. TEMPERATURE



NEGATIVE OUTPUT SWING vs. TEMPERATURE



Pin Description

PIN					NAME	FUNCTION
MAX4223/MAX4224		MAX4225 MAX4227	MAX4226/MAX4228			
SOT23	SO	SO	µMAX	SO		
—	1, 5	—	—	5, 7, 8, 10	N.C.	No Connect. Not internally connected. Tie to GND for optimum AC performance.
1	6	—	—	—	OUT	Amplifier Output
2	4	4	4	4	V_{EE}	Negative Power-Supply Voltage. Connect to -5V.
3	3	—	—	—	IN+	Amplifier Noninverting Input
4	2	—	—	—	IN-	Amplifier Inverting Input
5	8	—	—	—	$\overline{SHDN}$	Amplifier Shutdown. Connect to +5V for normal operation. Connect to GND for low-power shutdown.
6	7	8	10	14	V_{CC}	Positive Power-Supply Voltage. Connect to +5V.
—	—	1	1	1	OUTA	Amplifier A Output
—	—	2	2	2	INA-	Amplifier A Inverting Input
—	—	3	3	3	INA+	Amplifier A Noninverting Input
—	—	5	7	11	INB+	Amplifier B Noninverting Input
—	—	6	8	12	INB-	Amplifier B Inverting Input
—	—	7	9	13	OUTB	Amplifier B Output
—	—	—	5	6	$\overline{SHDNA}$	Amplifier A Shutdown Input. Connect to +5V for normal operation. Connect to GND for low-power shutdown mode.
—	—	—	6	9	$\overline{SHDNB}$	Amplifier B Shutdown Input. Connect to +5V for normal operation. Connect to GND for low-power shutdown mode.

Detailed Description

The MAX4223–MAX4228 are ultra-high-speed, low-power, current-feedback amplifiers featuring -3dB bandwidths up to 1GHz, 0.1dB gain flatness up to 300MHz, and very low differential gain and phase errors of 0.01% and 0.02°, respectively. These devices operate on dual ±5V or ±3V power supplies and require only 6mA of supply current per amplifier. The MAX4223/MAX4225/MAX4226 are optimized for closed-loop gains of +1 (0dB) or more and have -3dB bandwidths of 1GHz. The MAX4224/MAX4227/MAX4228 are optimized for closed-loop gains of +2 (6dB) or more, and have -3dB bandwidths of 600MHz (1.2GHz gain-bandwidth product).

The current-mode feedback topology of these amplifiers allows them to achieve slew rates of up to 1700V/µs with corresponding large signal bandwidths up to 330MHz. Each device in this family has an output that is capable of driving a minimum of 60mA of output current to ±2.5V.

Theory of Operation

Since the MAX4223–MAX4228 are current-feedback amplifiers, their open-loop transfer function is expressed as a transimpedance:

$$\frac{\Delta V_{OUT}}{\Delta I_{IN-}} \text{ or } T_Z$$

The frequency behavior of this open-loop transimpedance is similar to the open-loop gain of a voltage-feedback amplifier. That is, it has a large DC value and decreases at approximately 6dB per octave.

Analyzing the current-feedback amplifier in a gain configuration (Figure 1) yields the following transfer function:

$$\frac{V_{OUT}}{V_{IN}} = G \times \frac{T_Z(S)}{T_Z(S) + G \times R_{IN-} + R_F}$$

where $G = A_V = 1 + \frac{R_F}{R_G}$.

At low gains, ($G \times R_{IN-}$) << R_F . Therefore, unlike traditional voltage-feedback amplifiers, the closed-loop bandwidth is essentially independent of the closed-loop gain. Note also that at low frequencies, T_Z >> [($G \times R_{IN-}$) + R_F], so that:

$$\frac{V_{OUT}}{V_{IN}} = G = 1 + \frac{R_F}{R_G}$$

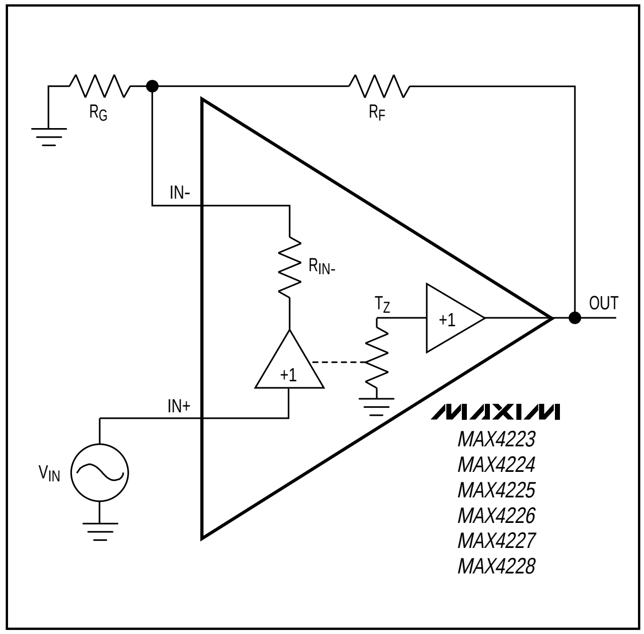


Figure 1. Current-Feedback Amplifier

Low-Power Shutdown Mode

The MAX4223/MAX4224/MAX4226/MAX4228 have a shutdown mode that is activated by driving the $\overline{SHDN}$ input low. When powered from ±5V supplies, the $\overline{SHDN}$ input is compatible with TTL logic. Placing the amplifier in shutdown mode reduces quiescent supply current to 350µA typical, and puts the amplifier output into a high-impedance state (100kΩ typical). This feature allows these devices to be used as multiplexers in wideband systems. To implement the mux function, the outputs of multiple amplifiers can be tied together, and only the amplifier with the selected input will be enabled. All of the other amplifiers will be placed in the low-power shutdown mode, with their high output impedance presenting very little load to the active amplifier output. For gains of +2 or greater, the feedback network impedance of all the amplifiers used in a mux application must be considered when calculating the total load on the active amplifier output.

Applications Information

Layout and Power-Supply Bypassing

The MAX4223–MAX4228 have an extremely high bandwidth, and consequently require careful board layout, including the possible use of constant-impedance microstrip or stripline techniques.

To realize the full AC performance of these high-speed amplifiers, pay careful attention to power-supply bypassing and board layout. The PC board should have at least two layers: a signal and power layer on one side and a large, low-impedance ground plane on the other. The ground plane should be as free of voids as possible, with one exception: the inverting input pin (IN-) should have as low a capacitance to ground as possible. This means that there should be no ground plane under IN- or under the components (R_F and R_G) connected to it. With multilayer boards, locate the ground plane on a layer that incorporates no signal or power traces.

Whether or not a constant-impedance board is used, it is best to observe the following guidelines when designing the board:

1) Do not use wire-wrapped boards (they are too inductive) or breadboards (they are too capacitive).
2) Do not use IC sockets. IC sockets increase reactance.
3) Keep signal lines as short and straight as possible. Do not make 90° turns; round all corners.
4) Observe high-frequency bypassing techniques to maintain the amplifier's accuracy and stability.
5) In general, surface-mount components have shorter bodies and lower parasitic reactance, giving better high-frequency performance than through-hole components.

The bypass capacitors should include a 10nF ceramic, surface-mount capacitor between each supply pin and the ground plane, located as close to the package as possible. Optionally, place a 10µF tantalum capacitor at the power-supply pins' point of entry to the PC board to ensure the integrity of incoming supplies. The power-supply trace should lead directly from the tantalum capacitor to the V_{CC} and V_{EE} pins. To minimize parasitic inductance, keep PC traces short and use surface-mount components. The N.C. pins should be connected to a common ground plane on the PC board to minimize parasitic coupling.

If input termination resistors and output back-termination resistors are used, they should be surface-mount types, and should be placed as close to the IC pins as possible. Tie all N.C. pins to the ground plane to minimize parasitic coupling.

Choosing Feedback and Gain Resistors

As with all current-feedback amplifiers, the frequency response of these devices depends critically on the value of the feedback resistor R_F. R_F combines with an internal compensation capacitor to form the dominant pole in the feedback loop. Reducing R_F's value increases the pole frequency and the -3dB bandwidth, but also increases peaking due to interaction with other nondominant poles. Increasing R_F's value reduces peaking and bandwidth.

Table 1 shows optimal values for the feedback resistor (R_F) and gain-setting resistor (R_G) for the MAX4223–MAX4228. Note that the MAX4224/MAX4227/MAX4228 offer superior AC performance for all gains except unity gain (0dB). These values provide optimal AC response using surface-mount resistors and good layout techniques. Maxim's high-speed amplifier evaluation kits provide practical examples of such layout techniques.

Stray capacitance at IN- causes feedback resistor decoupling and produces peaking in the frequency-response curve. Keep the capacitance at IN- as low as possible by using surface-mount resistors and by avoiding the use of a ground plane beneath or beside these resistors and the IN- pin. Some capacitance is unavoidable; if necessary, its effects can be counteracted by adjusting R_F. Use 1% resistors to maintain consistency over a wide range of production lots.

Table 1. Optimal Feedback Resistor Networks

GAIN (V/V)	GAIN (dB)	R_F (Ω)	R_G (Ω)	-3dB BW (MHz)	0.1dB BW (MHz)
MAX4223/MAX4225/MAX4226					
1	0	560*	Open	1000	300
2	6	200	200	380	115
5	14	100	25	235	65
MAX4224/MAX4227/MAX4228					
2	6	470	470	600	200
5	14	240	62	400	90
10	20	130	15	195	35

**For the MAX4223EUT, this optimal value is 470Ω.*

DC and Noise Errors

The MAX4223–MAX4228 output offset voltage, V_{OUT} (Figure 2), can be calculated with the following equation:

$$V_{OUT} = V_{OS} \times \left(1 + R_F/R_G\right) + I_{B+} \times R_S \times \left(1 + \frac{R_F}{R_G}\right) + I_{B-} \times R_F$$

where:

V_{OS} = input offset voltage (in volts)

$1 + R_F / R_G$ = amplifier closed-loop gain (dimensionless)

I_{B+} = input bias current (in amps)

I_{B-} = inverting input bias current (in amps)

R_G = gain-setting resistor (in Ω)

R_F = feedback resistor (in Ω)

R_S = source resistor (in Ω)

The following equation represents output noise density:

$$e_{n(OUT)} = \left(1 + \frac{R_F}{R_G}\right) \times \sqrt{\left(i_{n+} \times R_S\right)^2 + \left[i_{n-} \times \left(R_F \parallel R_G\right)\right]^2 + \left(e_n\right)^2}$$

where:

i_n = input noise current density (in pA/√Hz)

e_n = input noise voltage density (in nV/√Hz)

The MAX4223–MAX4228 have a very low, 2nV/√Hz noise voltage. The current noise at the noninverting input (i_{n+}) is 3pA/√Hz, and the current noise at the inverting input (i_{n-}) is 20pA/√Hz.

An example of DC-error calculations, using the MAX4224 typical data and the typical operating circuit with $R_F = R_G = 470Ω$ ($R_F \parallel R_G = 235Ω$) and $R_S = 50Ω$, gives:

$$V_{OUT} = [5 \times 10^{-4} \times (1 + 1)] + [2 \times 10^{-6} \times 50 \times (1 + 1)] + [4 \times 10^{-6} \times 470]$$

$$V_{OUT} = 3.1mV$$

Calculating total output noise in a similar manner yields the following:

$$e_{n(OUT)} = (1 + 1) \times \sqrt{\left[\left(3 \times 10^{-12}\right) \times 50\right]^2 + \left[\left(20 \times 10^{-12}\right) \times 235\right]^2 + \left(2 \times 10^{-9}\right)^2}$$

$$e_{n(OUT)} = 10.2nV / \sqrt{Hz}$$

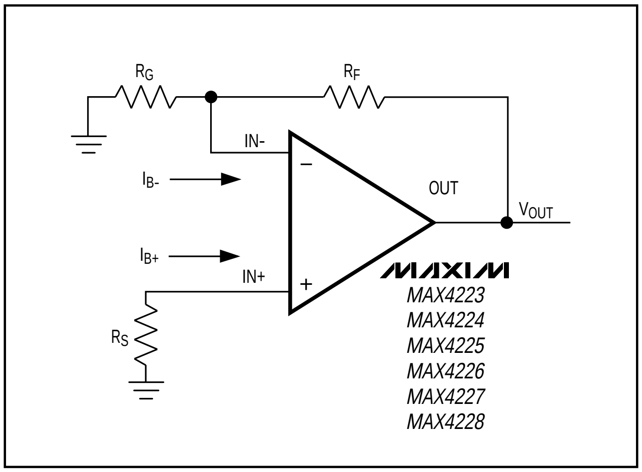


Figure 2. Output Offset Voltage

With a 600MHz system bandwidth, this calculates to $250µV_{RMS}$ (approximately 1.5mVp-p, using the six-sigma calculation).

Communication Systems

Nonlinearities of components used in a communication system produce distortion of the desired output signal. Intermodulation distortion (IMD) is the distortion that results from the mixing of two input signals of different frequencies in a nonlinear system. In addition to the input signal frequencies, the resulting output signal contains new frequency components that represent the sum and difference products of the two input frequencies. If the two input signals are relatively close in frequency, the third-order sum and difference products will fall close to the frequency of the desired output and will therefore be very difficult to filter. The third-order intercept (IP3) is defined as the power level at which the amplitude of the largest third-order product is equal to the power level of the desired output signal. Higher third-order intercept points correspond to better linearity of the amplifier. The MAX4223–MAX4228 have a typical IP3 value of 42dBm, making them excellent choices for use in communications systems.

ADC Input Buffers

Input buffer amplifiers can be a source of significant errors in high-speed ADC applications. The input buffer is usually required to rapidly charge and discharge the ADC's input, which is often capacitive (see the section *Driving Capacitive Loads*). In addition, a high-speed ADC's input impedance often changes very rapidly during the conversion cycle, requiring an amplifier with very low output impedance at high frequencies to maintain measurement accuracy. The combination of high speed, fast slew rate, low noise, and low distortion makes the MAX4223–MAX4228 ideally suited for use as buffer amplifiers in high-speed ADC applications.

Video Line Driver

The MAX4223–MAX4228 are optimized to drive coaxial transmission lines when the cable is terminated at both ends, as shown in Figure 3. Note that cable frequency response may cause variations in the signal's flatness.

Driving Capacitive Loads

A correctly terminated transmission line is purely resistive and presents no capacitive load to the amplifier. Although the MAX4223–MAX4228 are optimized for AC performance and are not designed to drive highly capacitive loads, they are capable of driving up to 25pF without excessive ringing. Reactive loads decrease phase margin and may produce excessive ringing and oscillation (see *Typical Operating Characteristics*). Figure 4's circuit reduces the effect of large capacitive loads. The small (usually 5Ω to 20Ω) isolation resistor R_{ISO}, placed before the reactive load, prevents ringing and oscillation at the expense of a small gain error. At higher capacitive loads, AC performance is limited by the interaction of load capacitance with the isolation resistor.

Maxim's High-Speed Evaluation Board Layout

Figures 7 and 8 show a suggested layout for Maxim's high-speed, single-amplifier evaluation boards. These boards were developed using the techniques described above. The smallest available surface-mount resistors were used for the feedback and back-termination resistors to minimize the distance from the IC to these resistors, thus reducing the capacitance associated with longer lead lengths.

SMA connectors were used for best high-frequency performance. Because distances are extremely short, performance is unaffected by the fact that inputs and outputs do not match a 50Ω line. However, in applications that require lead lengths greater than 1/4 of the wavelength of the highest frequency of interest, constant-impedance traces should be used.

Fully assembled evaluation boards are available for the MAX4223 in an SO-8 package.

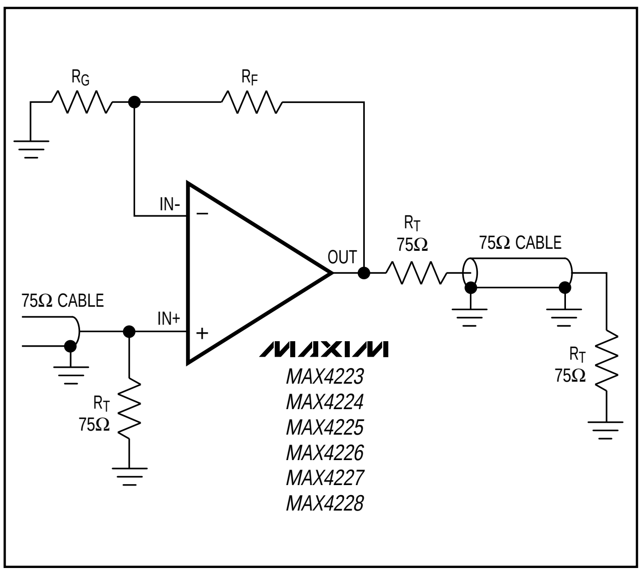


Figure 3. Video Line Driver

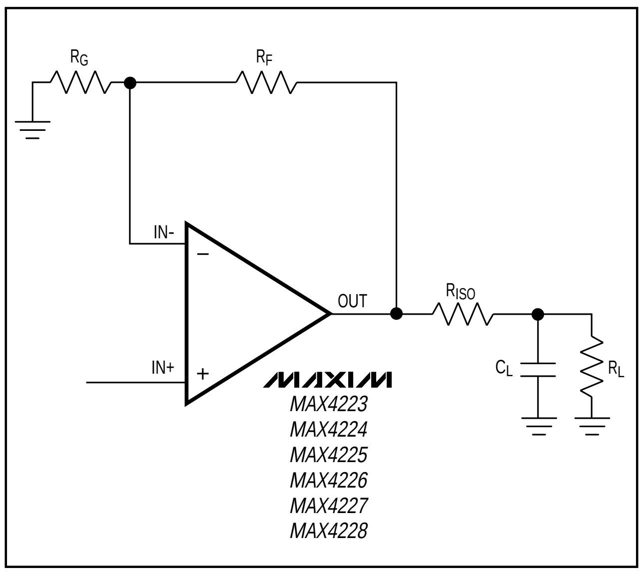


Figure 4. Using an Isolation Resistor (R_{ISO}) for High Capacitive Loads

1GHz, Low-Power, SOT23, Current-Feedback Amplifiers with Shutdown

AC Testing/Performance

AC specifications on high-speed amplifiers are usually guaranteed without 100% production testing. Since these high-speed devices are sensitive to external parasitics introduced when automatic handling equipment is used, it is impractical to guarantee AC parameters through volume production testing. These parasitics are greatly reduced when using the recommended PC board layout (like the Maxim evaluation kit). Characterizing the part in this way more accurately represents the amplifier's true AC performance. Some manufacturers guarantee AC specifications without clearly stating how this guarantee is made. The MAX4223–MAX4228 AC specifications are derived from worst-case design simulations combined with a sample characterization of 100 units. The AC performance distributions along with the worst-case simulation limits are shown in Figures 5 and 6. These distributions are repeatable provided that proper board layout and power-supply bypassing are used (see *Layout and Power-Supply Bypassing* section).

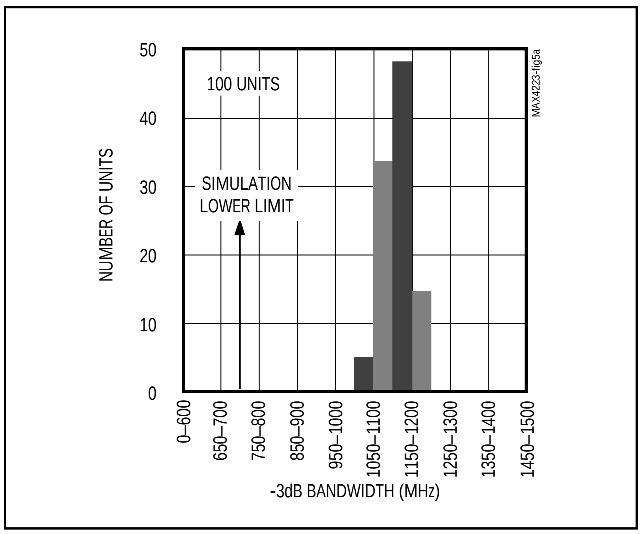


Figure 5a. MAX4223 -3dB Bandwidth Distribution

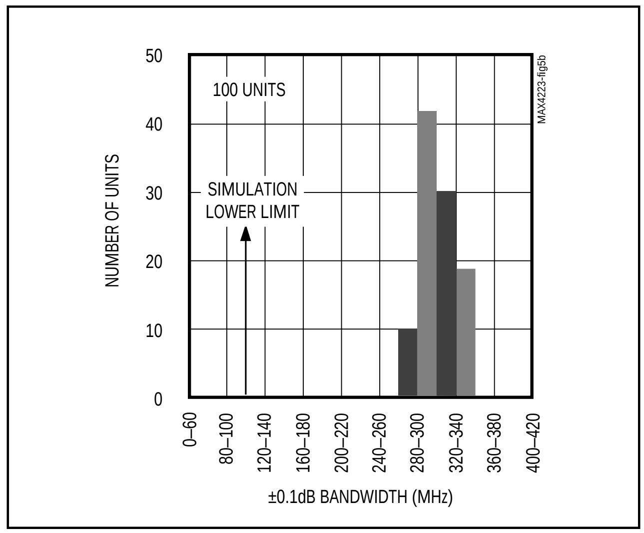


Figure 5b. MAX4223 ±0.1dB Bandwidth Distribution

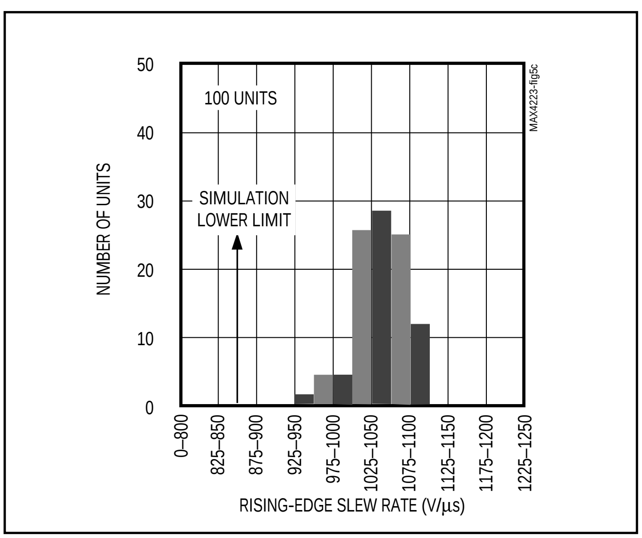


Figure 5c. MAX4223 Rising-Edge Slew-Rate Distribution

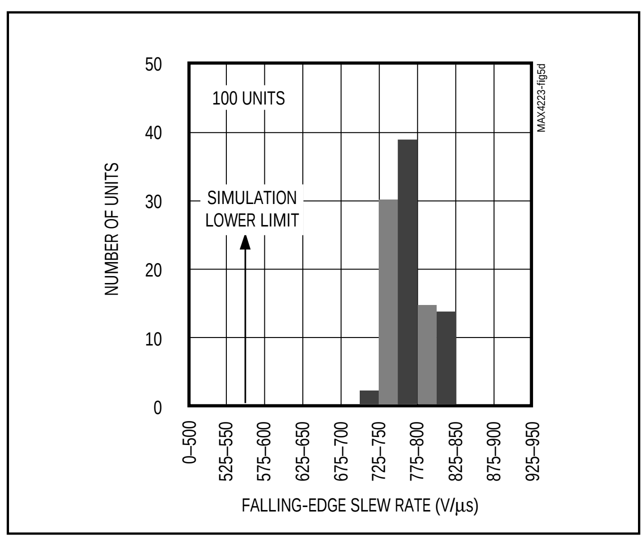


Figure 5d. MAX4223 Falling-Edge Slew-Rate Distribution

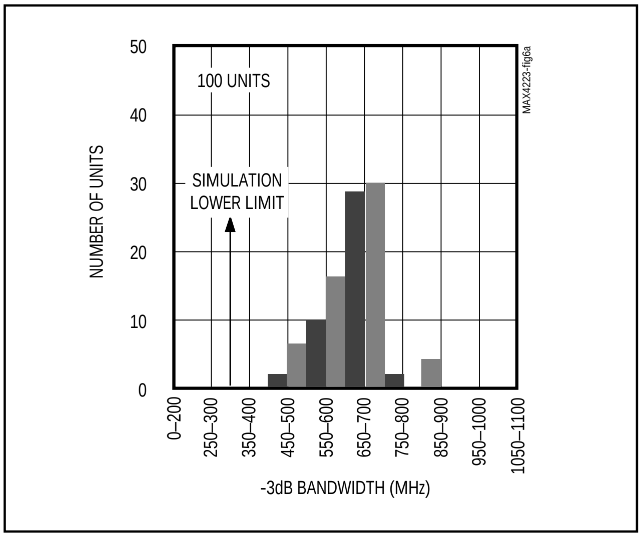


Figure 6a. MAX4224 -3dB Bandwidth Distribution

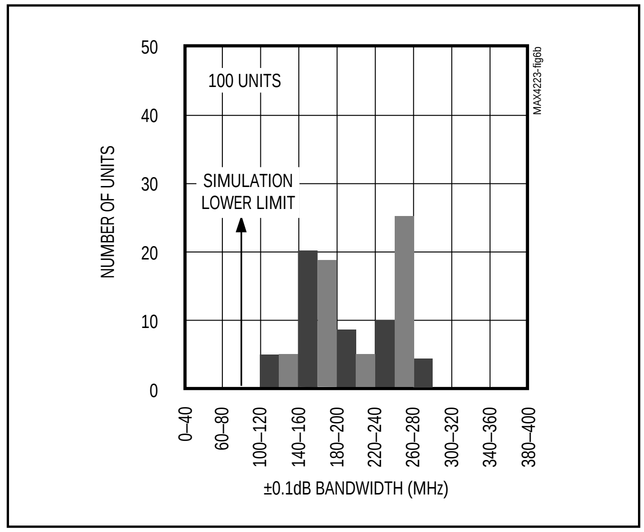


Figure 6b. MAX4224 ±0.1dB Bandwidth Distribution

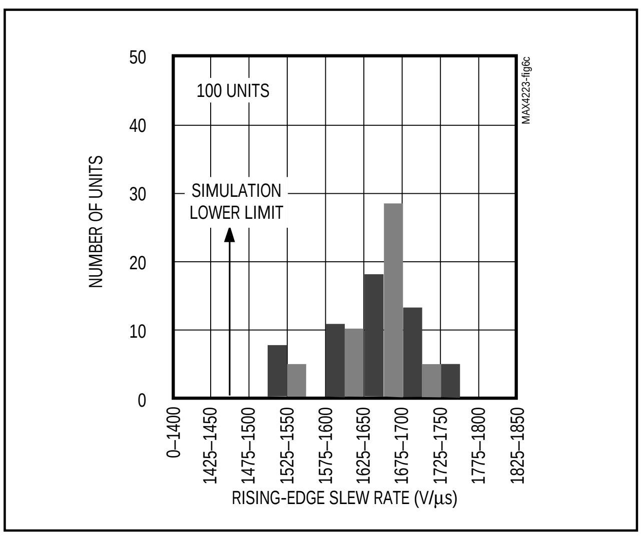


Figure 6c. MAX4224 Rising-Edge Slew-Rate Distribution

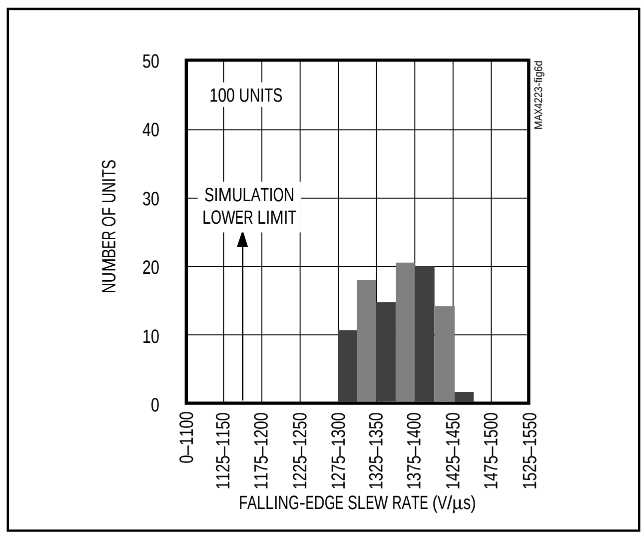


Figure 6d. MAX4224 Falling-Edge Slew-Rate Distribution

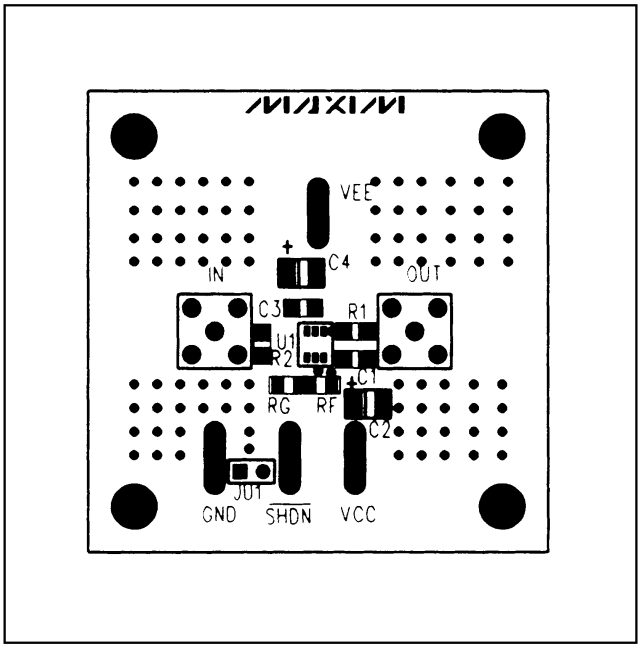


Figure 7a. Maxim SOT23 High-Speed Evaluation Board Component Placement Guide—Component Side

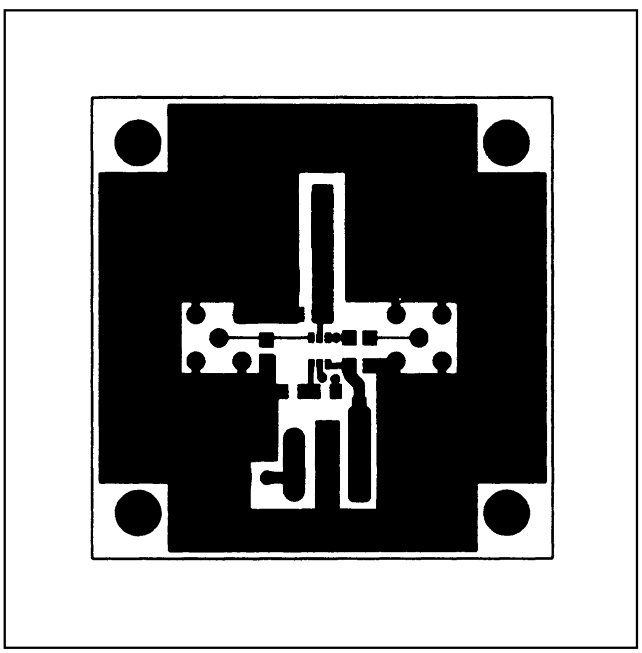


Figure 7b. Maxim SOT23 High-Speed Evaluation Board PC Board Layout—Component Side

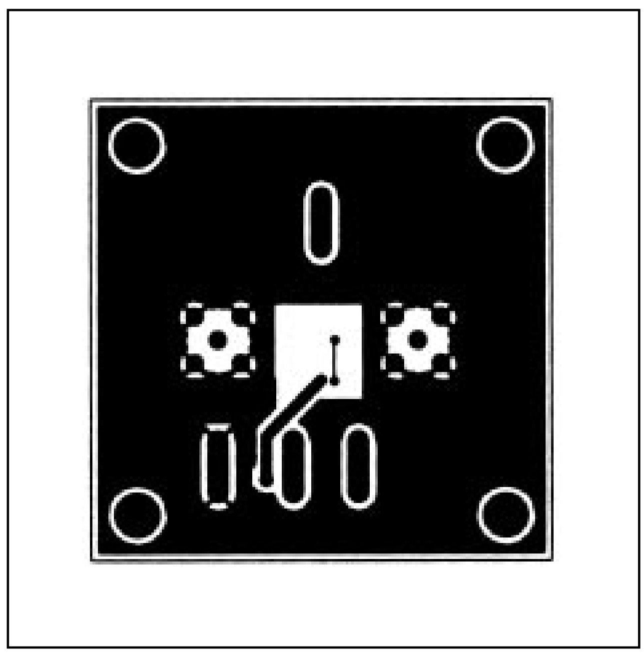


Figure 7c. Maxim SOT23 High-Speed Evaluation Board PC Board Layout—Back Side

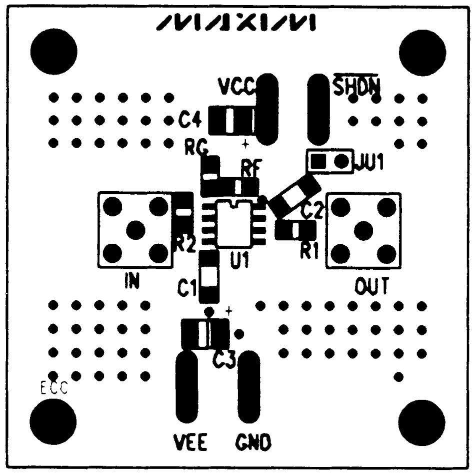


Figure 8a. Maxim SO-8 High-Speed Evaluation Board Component Placement Guide—Component Side

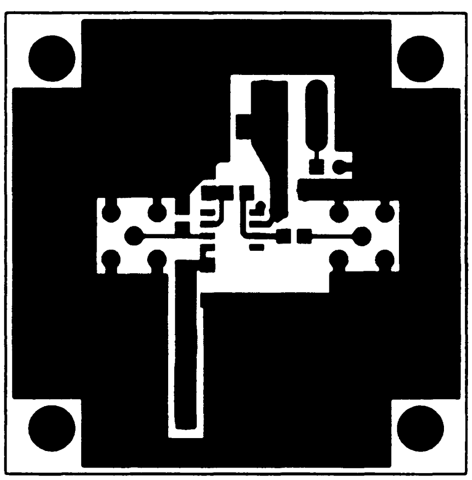


Figure 8b. Maxim SO-8 High-Speed Evaluation Board PC Board Layout—Component Side

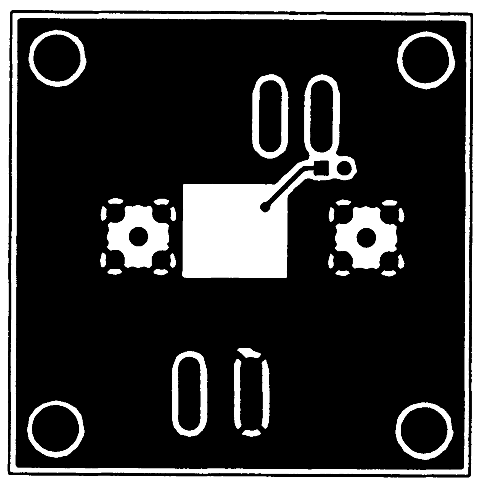
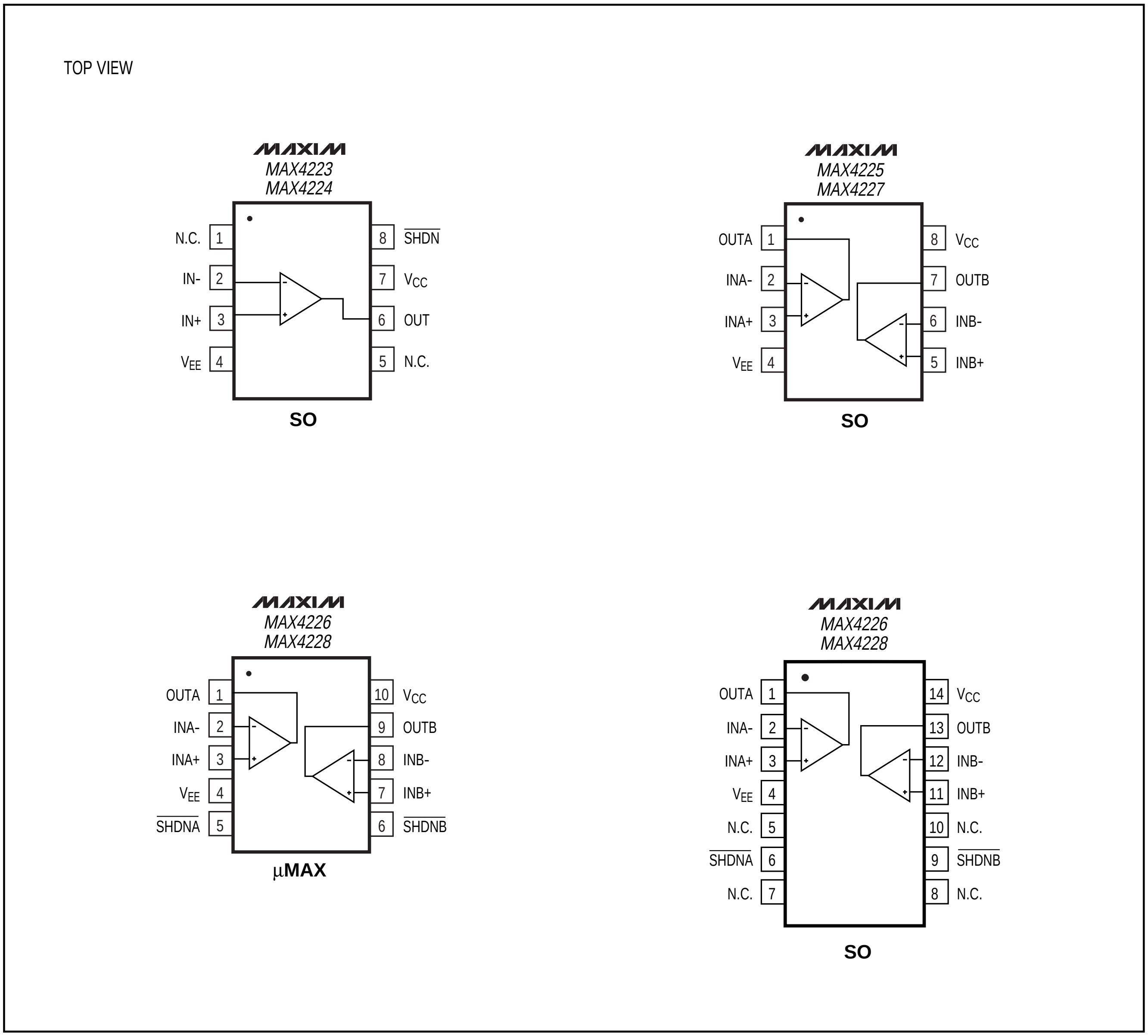


Figure 8c. Maxim SO-8 High-Speed Evaluation Board PC Board Layout—Back Side

Pin Configurations (continued)



Ordering Information (continued)

PART	TEMP. RANGE	PIN-PACKAGE	SOT TOP MARK
MAX4224EUT-T	-40°C to +85°C	6 SOT23	AAAE
MAX4224ESA	-40°C to +85°C	8 SO	—
MAX4225ESA	-40°C to +85°C	8 SO	—
MAX4226EUB	-40°C to +85°C	10 µMAX	—
MAX4226ESD	-40°C to +85°C	14 SO	—
MAX4227ESA	-40°C to +85°C	8 SO	—
MAX4228EUB	-40°C to +85°C	10 µMAX	—
MAX4228ESD	-40°C to +85°C	14 SO	—

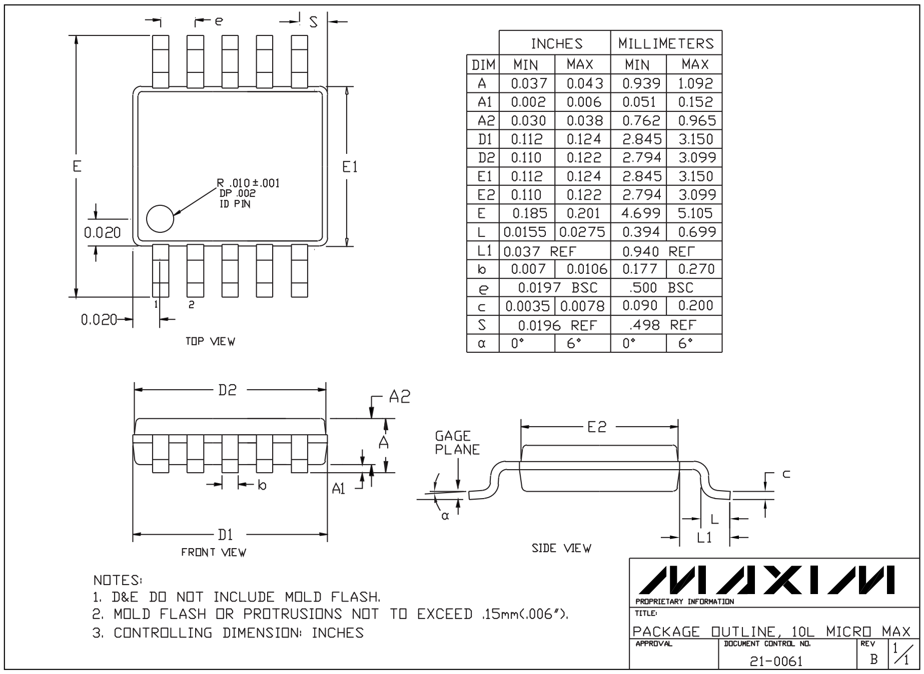
Chip Information

MAX4223/MAX4224 TRANSISTOR COUNT: 87

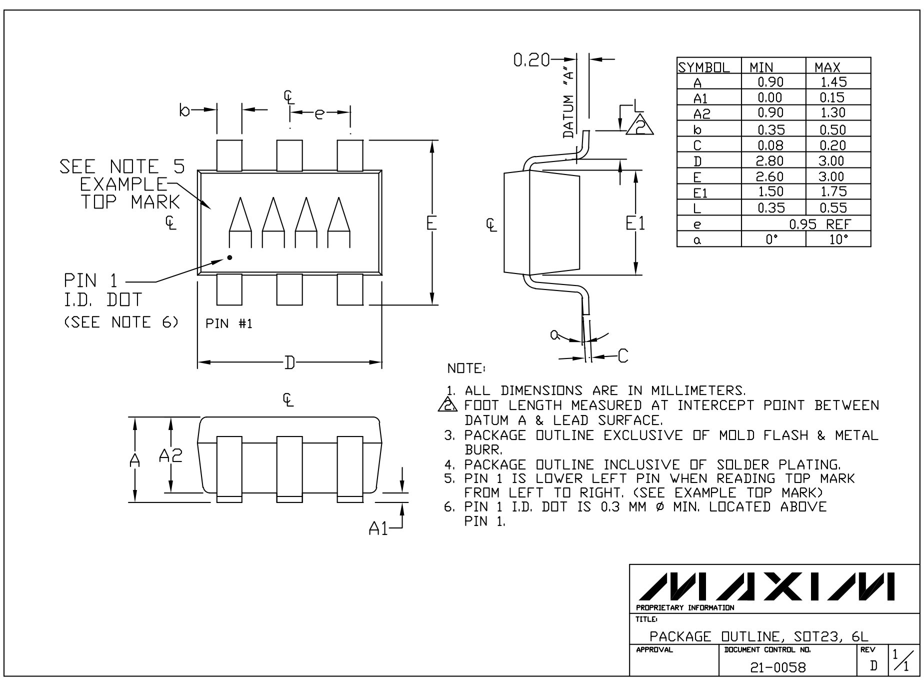
MAX4225–MAX4228 TRANSISTOR COUNT: 171

SUBSTRATE CONNECTED TO V_{EE}

Package Information



	INCHES		MILLIMETERS	
DIM	MIN	MAX	MIN	MAX
A	0.037	0.043	0.939	1.092
A1	0.002	0.006	0.051	0.152
A2	0.030	0.038	0.762	0.965
D1	0.112	0.124	2.845	3.150
D2	0.110	0.122	2.794	3.099
E1	0.112	0.124	2.845	3.150
E2	0.110	0.122	2.794	3.099
E	0.185	0.201	4.699	5.105
L	0.0155	0.0275	0.394	0.699
L1	0.037 REF		0.940 REF	
b	0.007	0.0106	0.177	0.270
e	0.0197 BSC		.500 BSC	
c	0.0035	0.0078	0.090	0.200
S	0.0196 REF		.498 REF	
α	0°	6°	0°	6°



SYMBOL	MIN	MAX
A	0.90	1.45
A1	0.00	0.15
A2	0.90	1.30
b	0.35	0.50
C	0.08	0.20
D	2.80	3.00
E	2.60	3.00
E1	1.50	1.75
L	0.35	0.55
e	0.95 REF	
α	0°	10°

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